

## FEATURES

- Single 5V Supply
- Sample Rate: 100ksps
- 8-Channel Multiplexer with  $\pm 30\text{V}$  Protection
- $\pm 10\text{V}$  Bipolar Input Range  
Single Ended or Differential
- $\pm 3\text{LSB}$  INL for the LTC1856,  $\pm 1.5\text{LSB}$  INL for the LTC1855,  $\pm 1\text{LSB}$  INL for the LTC1854
- Power Dissipation: 40mW (Typ)
- SPI/MICROWIRE™ Compatible Serial I/O
- Power Shutdown: Nap and Sleep
- SINAD: 87dB (LTC1856)
- Operates with Internal or External Reference
- Internal Synchronized Clock
- 28-Pin SSOP Package

## APPLICATIONS

- Industrial Process Control
- Multiplexed Data Acquisition Systems
- High Speed Data Acquisition for PCs
- Digital Signal Processing

## DESCRIPTION

The LTC®1854/LTC1855/LTC1856 are 8-channel, low power, 12-/14-/16-bit, 100ksps, analog-to-digital converters (ADCs). These ADCs operate from a single 5V supply and the 8-channel multiplexer can be programmed for single-ended inputs, pairs of differential inputs, or combinations of both. In addition, all channels are fault protected to  $\pm 30\text{V}$ . A fault condition on any channel will not affect the conversion result of the selected channel.

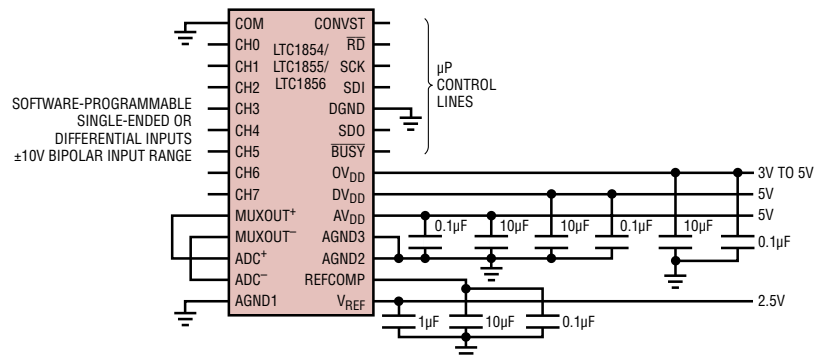
An onboard precision reference minimizes external components. Power dissipation is 40mW at 100ksps and lower in two power shutdown modes (27.5mW in Nap mode and 40 $\mu\text{W}$  in Sleep mode.) DC specifications include  $\pm 3\text{LSB}$  INL for the LTC1856,  $\pm 1.5\text{LSB}$  INL for the LTC1855 and  $\pm 1\text{LSB}$  for the LTC1854.

The internal clock is trimmed for 5 $\mu\text{s}$  maximum conversion time and the sampling rate is guaranteed at 100ksps. A separate convert start input and data ready signal ( $\overline{\text{BUSY}}$ ) ease connections to FIFOs, DSPs and microprocessors.

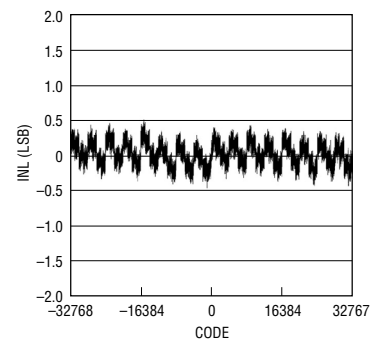
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## TYPICAL APPLICATION

100kHz, 12-Bit/14-/16-Bit Sampling ADC



LTC1856 Typical INL Curve



# LTC1854/LTC1855/LTC1856

## ABSOLUTE MAXIMUM RATINGS

(Notes 1, 2)

Supply Voltage ( $OV_{DD} = DV_{DD} = AV_{DD} = V_{DD}$ ) .....	6V
Ground Voltage Difference DGND, AGND1, AGND2, AGND3 .....	$\pm 0.3V$
Analog Input Voltage ADC <sup>+</sup> , ADC <sup>-</sup> (Note 3) .....	(AGND1 - 0.3V) to (AV <sub>DD</sub> + 0.3V)
CHO-CH7, COM .....	$\pm 30V$
Digital Input Voltage (Note 4) .....	(DGND - 0.3V) to 10V
Digital Output Voltage ....	(DGND - 0.3V) to (DV <sub>DD</sub> + 0.3V)
Power Dissipation .....	500mW
Operating Temperature Range LTC1854C/LTC1855C/LTC1856C .....	0°C to 70°C
LTC1854I/LTC1855I/LTC1856I .....	-40°C to 85°C
Storage Temperature Range .....	-65°C to 150°C
Lead Temperature (Soldering, 10 sec) .....	300°C

## PACKAGE/ORDER INFORMATION

TOP VIEW

COM [1]				[28] CONVST
CHO [2]				[27] RD
CH1 [3]				[26] SCK
CH2 [4]				[25] SDI
CH3 [5]				[24] DGND
CH4 [6]				[23] SDO
CH5 [7]				[22] BUSY
CH6 [8]				[21] OV <sub>DD</sub>
CH7 [9]				[20] DV <sub>DD</sub>
MUXOUT* [10]				[19] AV <sub>DD</sub>
MUXOUT* [11]				[18] AGND3
ADC* [12]				[17] AGND2
ADC* [13]				[16] REFCOMP
AGND1 [14]				[15] V <sub>REF</sub>

G PACKAGE  
28-LEAD PLASTIC SSOP

T<sub>JMAX</sub> = 125°C, θ<sub>JA</sub> = 160°C/W  
EXPOSED PAD (PIN #) IS GND, MUST BE SOLDERED TO PCB

### ORDER PART NUMBER

LTC1854CG	LTC1855CG	LTC1856CG
LTC1854IG	LTC1855IG	LTC1856IG

**Order Options** Tape and Reel: Add #TR  
Lead Free: Add #PBF Lead Free Tape and Reel: Add #TRPBF  
Lead Free Part Marking: <http://www.linear.com/leadfree/>

Consult LTC Marketing for parts specified with wider operating temperature ranges.

## CONVERTER AND MULTIPLEXER CHARACTERISTICS

The ● denotes the specifications which apply over the full operating temperature range, otherwise specifications are at T<sub>A</sub> = 25°C. MUXOUT connected to ADC inputs. (Notes 5, 6)

PARAMETER	CONDITIONS	LTC1854			LTC1855			LTC1856			UNITS
		MIN	TYP	MAX	MIN	TYP	MAX	MIN	TYP	MAX	
Resolution		●	12		14		15				Bits
No Missing Codes		●	12		14		15				Bits
Transition Noise				0.06		0.25		1			LSB <sub>RMS</sub>
Integral Linearity Error	(Note 7)	●		±1		±1.5		±3			LSB
Differential Linearity Error		●	-1	1	-1	1.5	-2	4			LSB
Bipolar Zero Error	(Note 8)	●		±5		±8		±23			LSB
Bipolar Zero Error Drift				±0.1		±0.1		±0.1			ppm/°C
Bipolar Zero Error Match				3		4		10			LSB
Bipolar Full-Scale Error	External Reference (Note 11) Internal Reference (Note 11)	●		±0.34 ±0.45		±0.14 ±0.40		±0.1 ±0.4			% %
Bipolar Full-Scale Error Drift	External Reference Internal Reference			±2.5 ±7		±2.5 ±7		±2.5 ±7			ppm/°C ppm/°C
Bipolar Full-Scale Error Match				5		10		15			LSB
Input Common Mode Range		●		±10		±10		±10			V
Input Common Mode Rejection Ratio				96		96		96			dB

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## ANALOG INPUT

The ● denotes the specifications which apply over the full operating temperature range, otherwise specifications are at  $T_A = 25^\circ\text{C}$ . (Note 5)

PARAMETER	CONDITIONS	MIN	TYP	MAX	UNITS
Analog Input Range	CH0 to CH7, COM		±10		V
	ADC <sup>+</sup> , ADC <sup>-</sup> (Note 3)		ADC <sup>-</sup> ±2.048		V
Impedance	CH0 to CH7, COM		31		k $\Omega$
	MUXOUT <sup>+</sup> , MUXOUT <sup>-</sup>		5		k $\Omega$
Capacitance	CH0 to CH7, COM		5		pF
	Sample Mode ADC <sup>+</sup> , ADC <sup>-</sup>		12		pF
	Hold Mode ADC <sup>+</sup> , ADC <sup>-</sup>		4		pF
Input Leakage Current	ADC <sup>+</sup> , ADC <sup>-</sup> , CONVST = Low	●		±1	$\mu\text{A}$

## DYNAMIC ACCURACY

The ● denotes the specifications which apply over the full operating temperature range, otherwise specifications are at  $T_A = 25^\circ\text{C}$ . MUXOUT connected to ADC inputs. (Note 5)

SYMBOL	PARAMETER	CONDITIONS	LTC1854			LTC1855			LTC1856			UNITS
			MIN	TYP	MAX	MIN	TYP	MAX	MIN	TYP	MAX	
S/(N + D)	Signal-to-(Noise + Distortion) Ratio	1kHz Input Signal		74			83			87		dB
THD	Total Harmonic Distortion	1kHz Input Signal First Five Harmonics		-102			-95			-101		dB
	Peak Harmonic or Spurious Noise	1kHz Input Signal		-99			-99			-103		dB
	Channel-to-Channel Isolation	1kHz Input Signal		-120			-120			-120		dB
	-3dB Input Bandwidth			1			1			1		MHz
	Aperture Delay			-70			-70			-70		ns
	Aperture Jitter			60			60			60		ps
	Transient Response	Full-Scale Step (Note 9)			4			4			4	$\mu\text{s}$
	Overvoltage Recovery	(Note 12)		150			150			150		ns

## INTERNAL REFERENCE CHARACTERISTICS

The ● denotes the specifications which apply over the full operating temperature range, otherwise specifications are at  $T_A = 25^\circ\text{C}$ . (Note 5)

PARAMETER	CONDITIONS		MIN	TYP	MAX	UNITS
$V_{REF}$ Output Voltage	$I_{OUT} = 0$	●	2.475	2.50	2.525	V
$V_{REF}$ Output Temperature Coefficient	$I_{OUT} = 0$			$\pm 10$		ppm/ $^\circ\text{C}$
$V_{REF}$ Output Impedance	$-0.1\text{mA} \leq I_{OUT} \leq 0.1\text{mA}$			8		$\text{k}\Omega$
$V_{REFCOMP}$ Output Voltage	$I_{OUT} = 0$			4.096		V

## DIGITAL INPUTS AND DIGITAL OUTPUTS

The ● denotes the specifications which apply over the full operating temperature range, otherwise specifications are at  $T_A = 25^\circ\text{C}$ . (Note 5)

SYMBOL	PARAMETER	CONDITIONS		MIN	TYP	MAX	UNITS
$V_{IH}$	High Level Input Voltage	$V_{DD} = 5.25\text{V}$	●	2.4			V
$V_{IL}$	Low Level Input Voltage	$V_{DD} = 4.75\text{V}$	●			0.8	V
$I_{IN}$	Digital Input Current	$V_{IN} = 0\text{V to } V_{DD}$	●			$\pm 10$	$\mu\text{A}$
$C_{IN}$	Digital Input Capacitance				5		pF
$V_{OH}$	High Level Output Voltage	$V_{DD} = 4.75\text{V}, I_O = -10\mu\text{A}, OV_{DD} = V_{DD}$ $V_{DD} = 4.75\text{V}, I_O = -200\mu\text{A}, OV_{DD} = V_{DD}$	●	4	4.74		V V
$V_{OL}$	Low Level Output Voltage	$V_{DD} = 4.75\text{V}, I_O = 160\mu\text{A}, OV_{DD} = V_{DD}$ $V_{DD} = 4.75\text{V}, I_O = 1.6\text{mA}, OV_{DD} = V_{DD}$	●		0.05 0.10	0.4	V V
$I_{OZ}$	Hi-Z Output Leakage	$V_{OUT} = 0\text{V to } V_{DD}, \overline{RD} = \text{High}$	●			$\pm 10$	$\mu\text{A}$
$C_{OZ}$	Hi-Z Output Capacitance	$\overline{RD} = \text{High}$			15		pF
$I_{SOURCE}$	Output Source Current	$V_{OUT} = 0\text{V}$			-10		mA
$I_{SINK}$	Output Sink Current	$V_{OUT} = V_{DD}$			10		mA

## POWER REQUIREMENTS

The ● denotes the specifications which apply over the full operating temperature range, otherwise specifications are at  $T_A = 25^\circ\text{C}$ . (Note 5)

PARAMETER	CONDITIONS		MIN	TYP	MAX	UNITS
Positive Supply Voltage	(Notes 9 and 10)		4.75	5.00	5.25	V
Positive Supply Current		●		8.0	12	mA
Nap Mode				5.5	7	mA
Sleep Mode	$CONVST = 0\text{V or } 5\text{V}$			8.0	13	$\mu\text{A}$
Power Dissipation				40.0		mW
Nap Mode				27.5		mW
Sleep Mode	$CONVST = 0\text{V or } 5\text{V}$			40.0		$\mu\text{W}$

## TIMING CHARACTERISTICS

The ● denotes the specifications which apply over the full operating temperature range, otherwise specifications are at  $T_A = 25^\circ\text{C}$ . (Note 5)

SYMBOL	PARAMETER	CONDITIONS	MIN	TYP	MAX	UNITS
$f_{\text{SAMPLE(MAX)}}$	Maximum Sampling Frequency	Through CH0 to CH7 Inputs Through ADC <sup>+</sup> , ADC <sup>-</sup> Only	● 100	166		kHz kHz
$t_{\text{CONV}}$	Conversion Time		●	4	5	$\mu\text{s}$
$t_{\text{ACQ}}$	Acquisition Time	Through CH0 to CH7 Inputs Through ADC <sup>+</sup> , ADC <sup>-</sup> Only	●	1	4	$\mu\text{s}$ $\mu\text{s}$
$f_{\text{SCK}}$	SCK Frequency	(Note 13)	● 0		20	MHz
$t_r$	SDO Rise Time	See Test Circuits		6		ns
$t_f$	SDO Fall Time	See Test Circuits		6		ns
$t_1$	CONVST High Time		● 40			ns
$t_2$	CONVST to $\overline{\text{BUSY}}$ Delay	$C_L = 25\text{pF}$ , See Test Circuits	●	15	30	ns
$t_3$	SCK Period		● 50			ns
$t_4$	SCK High		● 10			ns
$t_5$	SCK Low		● 10			ns
$t_6$	Delay Time, SCK $\downarrow$ to SDO Valid	$C_L = 25\text{pF}$ , See Test Circuits	●	25	45	ns
$t_7$	Time from Previous SDO Data Remains Valid After SCK $\downarrow$	$C_L = 25\text{pF}$ , See Test Circuits	● 5	20		ns
$t_8$	SDO Valid After $\overline{\text{RD}}\downarrow$	$C_L = 25\text{pF}$ , See Test Circuits	●	11	30	ns
$t_9$	$\overline{\text{RD}}\downarrow$ to SCK Setup Time		● 20			ns
$t_{10}$	SDI Setup Time Before SCK $\uparrow$		● 0			ns
$t_{11}$	SDI Hold Time After SCK $\uparrow$		● 7			ns
$t_{12}$	SDO Valid Before $\overline{\text{BUSY}}\uparrow$	$\overline{\text{RD}} = \text{Low}$ , $C_L = 25\text{pF}$ , See Test Circuits	● 5	20		ns
$t_{13}$	Bus Relinquish Time	See Test Circuits	●	10	30	ns

**Note 1:** Stresses beyond those listed under Absolute Maximum Ratings may cause permanent damage to the device. Exposure to any Absolute Maximum Rating condition for extended periods may affect device reliability and lifetime.

**Note 2:** All voltage values are with respect to ground with DGND, AGND1, AGND2 and AGND3 wired together unless otherwise noted.

**Note 3:** When these pin voltages are taken below ground or above  $AV_{DD} = DV_{DD} = OV_{DD} = V_{DD}$ , they will be clamped by internal diodes. This product can handle currents of greater than 100mA below ground or above  $V_{DD}$  without latchup.

**Note 4:** When these pin voltages are taken below ground they will be clamped by internal diodes. This product can handle currents of greater than 100mA below ground without latchup. These pins are not clamped to  $V_{DD}$ .

**Note 5:**  $V_{DD} = 5\text{V}$ ,  $f_{\text{SAMPLE}} = 100\text{kHz}$ ,  $t_r = t_f = 5\text{ns}$  unless otherwise specified.

**Note 6:** Linearity, offset and full-scale specifications apply for a single-ended analog MUX input with respect to ground or ADC<sup>+</sup> with respect to ADC<sup>-</sup> tied to ground.

**Note 7:** Integral nonlinearity is defined as the deviation of a code from a straight line passing through the actual end points of the transfer curve. The deviation is measured from the center of the quantization band.

**Note 8:** Bipolar zero error is the offset voltage measured from  $-0.5\text{LSB}$  when the output code flickers between 0000 0000 0000 0000 and 1111 1111 1111 1111 for the LTC1856, between 00 0000 0000 0000 and 11 1111 1111 1111 for the LTC1855 and between 0000 0000 0000 and 1111 1111 1111 for the LTC1854.

**Note 9:** Guaranteed by design, not subject to test.

**Note 10:** Recommended operating conditions.

**Note 11:** Full-scale bipolar error is the worst case of  $-FS$  or  $+FS$  untrimmed deviation from ideal first and last code transitions, divided by the full-scale range, and includes the effect of offset error.

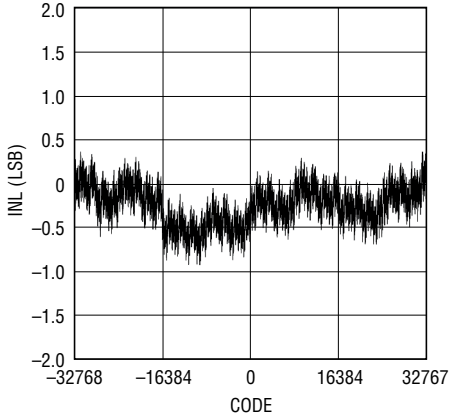
**Note 12:** Recovers to specified performance after  $(2 \cdot FS)$  input overvoltage.

**Note 13:**  $t_6$  of 45ns maximum allows  $f_{\text{SCK}}$  up to 10MHz for rising capture with 50% duty cycle and  $f_{\text{SCK}}$  up to 20MHz for falling capture (with 5ns setup time for the receiving logic).

# LTC1854/LTC1855/LTC1856

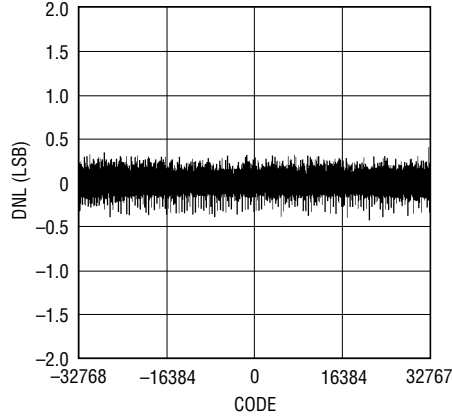
## TYPICAL PERFORMANCE CHARACTERISTICS

LTC1856 Typical INL Curve



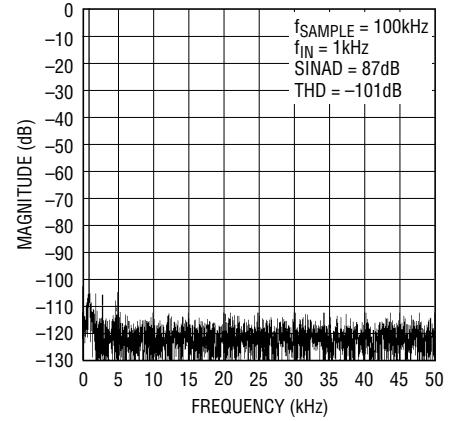
185456 G01

LTC1856 Typical DNL Curve



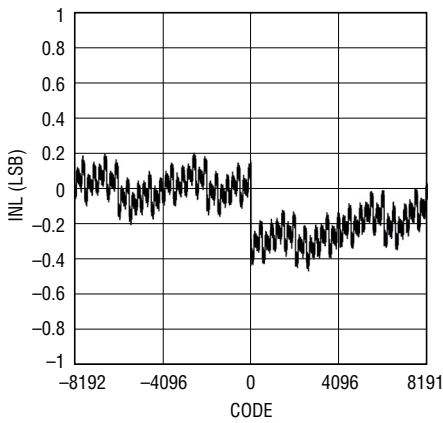
185456 G02

LTC1856 Nonaveraged 4096-Point FFT Plot



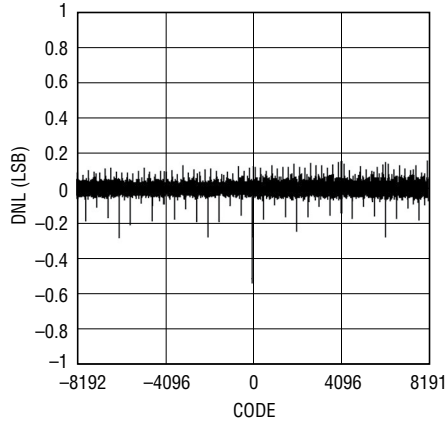
185456 G03

LTC1855 Typical INL Curve



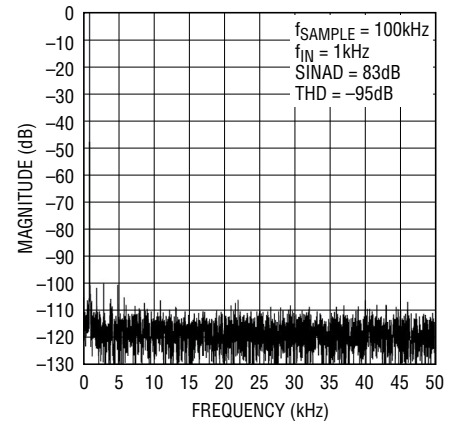
185455 G04

LTC1855 Typical DNL Curve



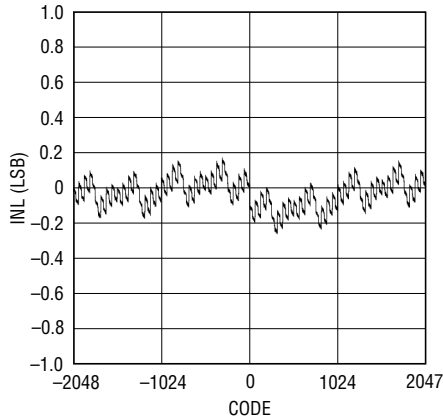
185456 G05

LTC1855 Nonaveraged 4096-Point FFT Plot



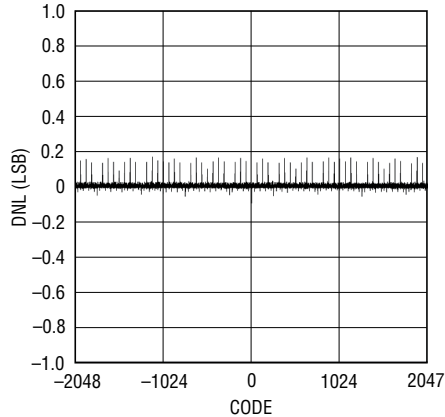
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LTC1854 Typical INL Curve



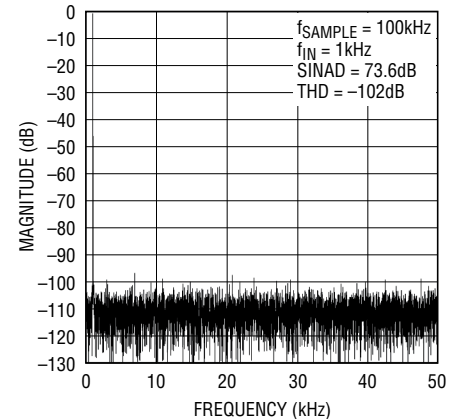
185456 G07

LTC1854 Typical DNL Curve



185456 G08

LTC1854 Nonaveraged 4096-Point FFT Plot

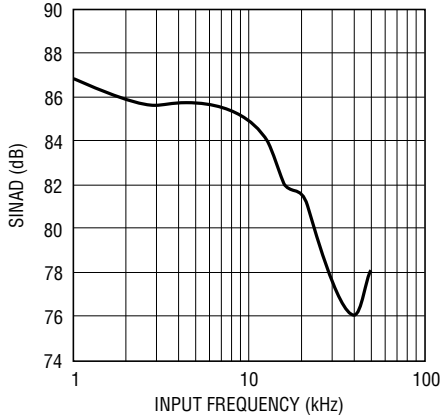


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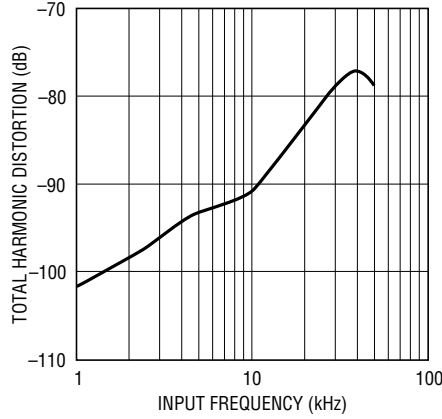
## TYPICAL PERFORMANCE CHARACTERISTICS

**LTC1856 SINAD vs Input Frequency**



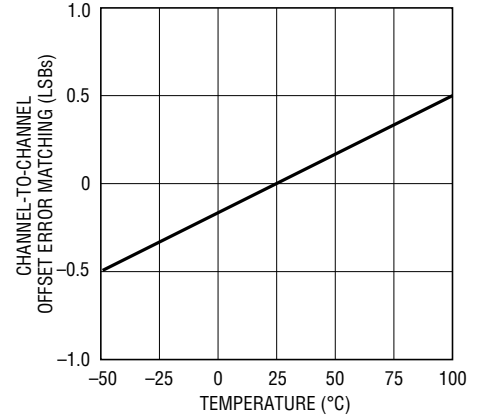
185456 G10

**LTC1856 Total Harmonic Distortion vs Input Frequency**



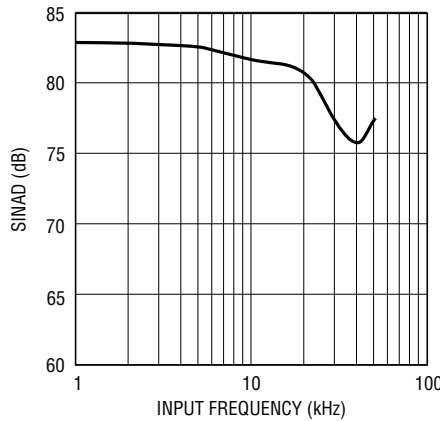
185456 G11

**LTC1856 Channel-to-Channel Offset Error Matching vs Temperature**



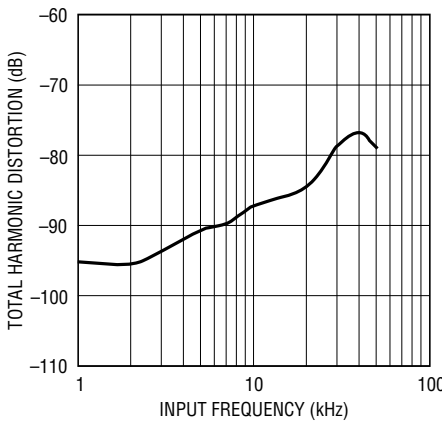
185456 G12

**LTC1855 SINAD vs Input Frequency**



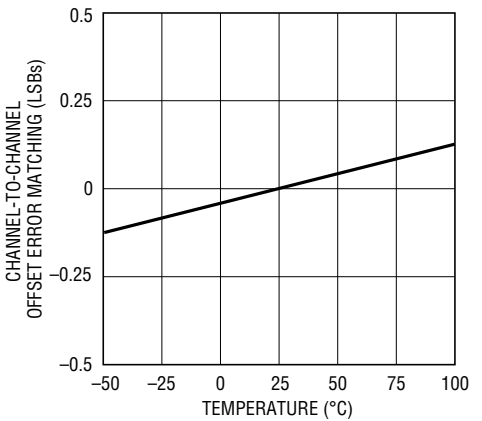
185456 G13

**LTC1855 Total Harmonic Distortion vs Input Frequency**



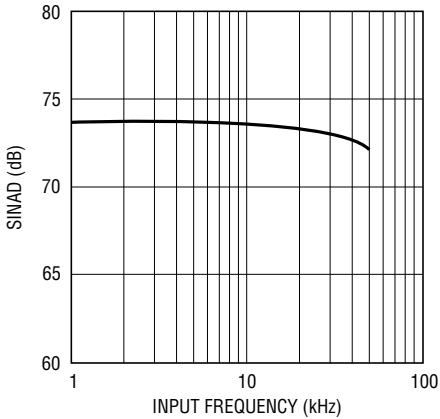
185456 G14

**LTC1855 Channel-to-Channel Offset Error Matching vs Temperature**



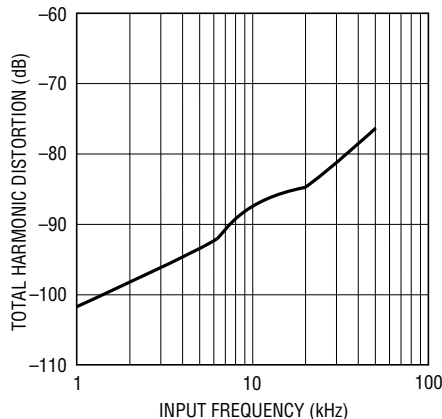
185456 G15

**LTC1854 SINAD vs Input Frequency**



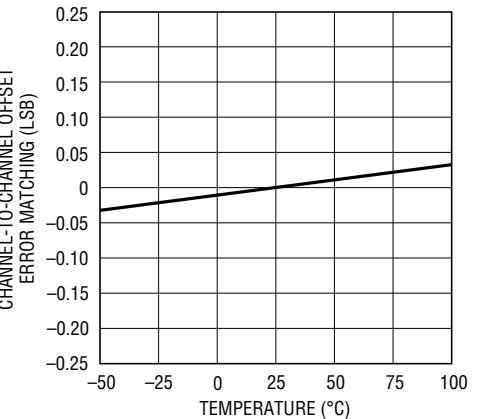
185456 G16

**LTC1854 Total Harmonic Distortion vs Input Frequency**



185456 G17

**LTC1854 Channel-to-Channel Offset Error Matching vs Temperature**

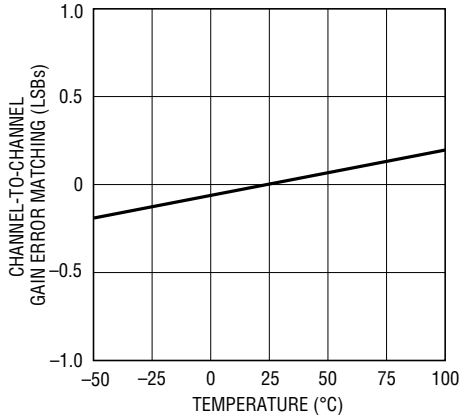


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# LTC1854/LTC1855/LTC1856

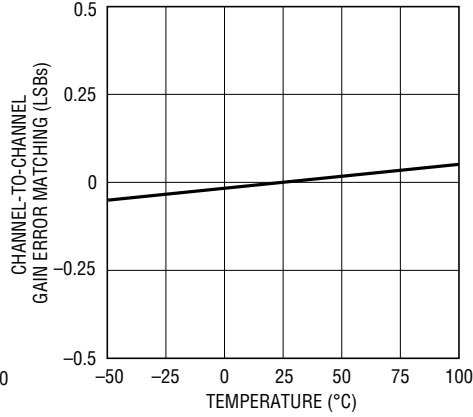
## TYPICAL PERFORMANCE CHARACTERISTICS

**LTC1856 Channel-to-Channel Gain Error Matching vs Temperature**



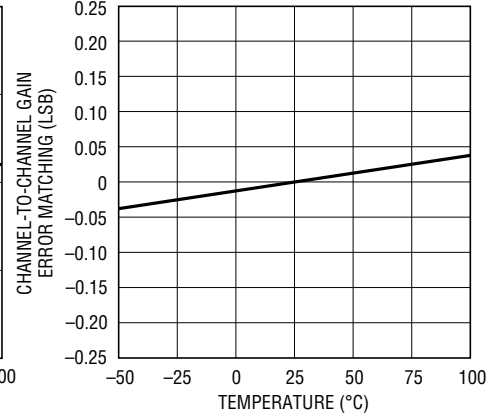
185456 G19

**LTC1855 Channel-to-Channel Gain Error Matching vs Temperature**



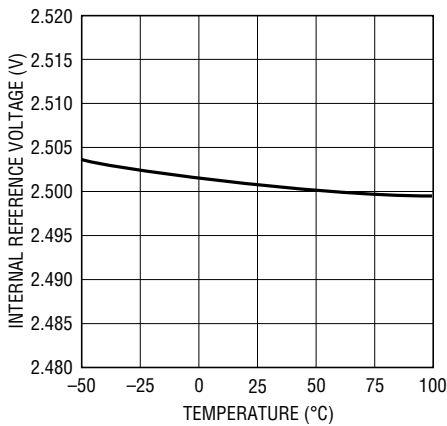
185456 G20

**LTC1854 Channel-to-Channel Gain Error Matching vs Temperature**



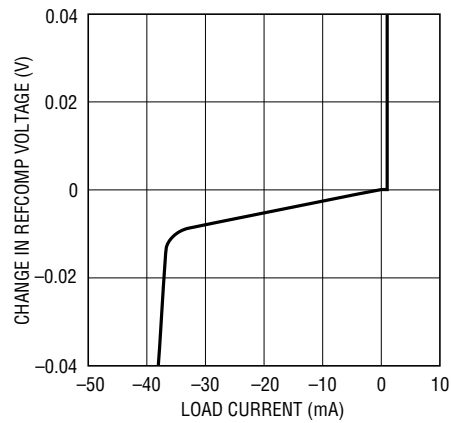
185456 G21

**Internal Reference Voltage vs Temperature**



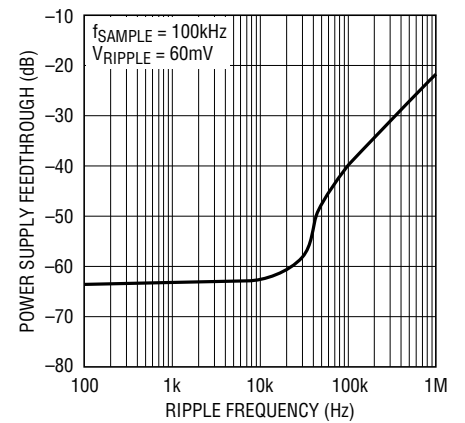
185456 G22

**Change in REFCOMP Voltage vs Load Current**



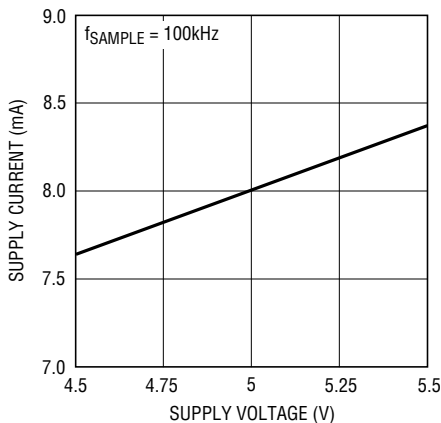
185456 G23

**LTC1856 Power Supply Feedthrough vs Ripple Frequency**



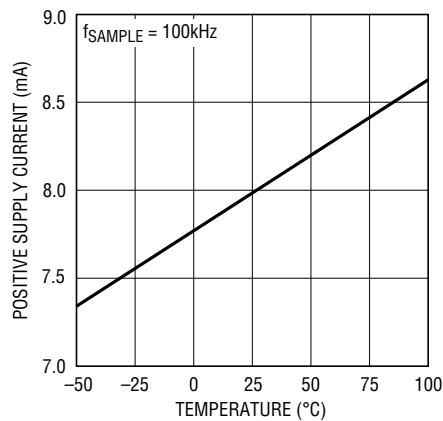
185456 G24

**Supply Current vs Supply Voltage**



185454 G25

**Supply Current vs Temperature**



185456 G26

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## PIN FUNCTIONS

**COM (Pin 1):** Common Input. This is the negative reference point for all single-ended inputs. It must be free of noise and is usually connected to the analog ground plane.

**CH0 (Pin 2):** Analog MUX Input.

**CH1 (Pin 3):** Analog MUX Input.

**CH2 (Pin 4):** Analog MUX Input.

**CH3 (Pin 5):** Analog MUX Input.

**CH4 (Pin 6):** Analog MUX Input.

**CH5 (Pin 7):** Analog MUX Input.

**CH6 (Pin 8):** Analog MUX Input.

**CH7 (Pin 9):** Analog MUX Input.

**MUXOUT<sup>+</sup> (Pin 10):** Positive MUX Output. Output of the analog multiplexer. Connect to ADC<sup>+</sup> for normal operation.

**MUXOUT<sup>-</sup> (Pin 11):** Negative MUX Output. Output of the analog multiplexer. Connect to ADC<sup>-</sup> for normal operation.

**ADC<sup>+</sup> (Pin 12):** Positive Analog Input to the Analog-to-Digital Converter.

**ADC<sup>-</sup> (Pin 13):** Negative Analog Input to the Analog-to-Digital Converter.

**AGND1 (Pin 14):** Analog Ground.

**V<sub>REF</sub> (Pin 15):** 2.5V Reference Output. Bypass to analog ground with a 1 $\mu$ F tantalum capacitor.

**REFCOMP (Pin 16):** Reference Buffer Output. Bypass to analog ground with a 10 $\mu$ F tantalum and a 0.1 $\mu$ F ceramic capacitor. Nominal output voltage is 4.096V.

**AGND2 (Pin 17):** Analog Ground.

**AGND3 (Pin 18):** Analog Ground. This is the substrate connection.

**AV<sub>DD</sub> (Pin 19):** 5V Analog Supply. Bypass to analog ground with a 0.1 $\mu$ F ceramic and a 10 $\mu$ F tantalum capacitor.

**DV<sub>DD</sub> (Pin 20):** 5V Digital Supply. Bypass to digital ground with a 0.1 $\mu$ F ceramic and a 10 $\mu$ F tantalum capacitor.

**OV<sub>DD</sub> (Pin 21):** Positive Supply for the Digital Output Buffers (3V to 5V). Bypass to digital ground with a 0.1 $\mu$ F ceramic and a 10 $\mu$ F tantalum capacitor.

**BUSY (Pin 22):** Output shows converter status. It is low when a conversion is in progress.

**SDO (Pin 23):** Serial Data Output.

## PIN FUNCTIONS

**DGND (Pin 24):** Digital Ground.

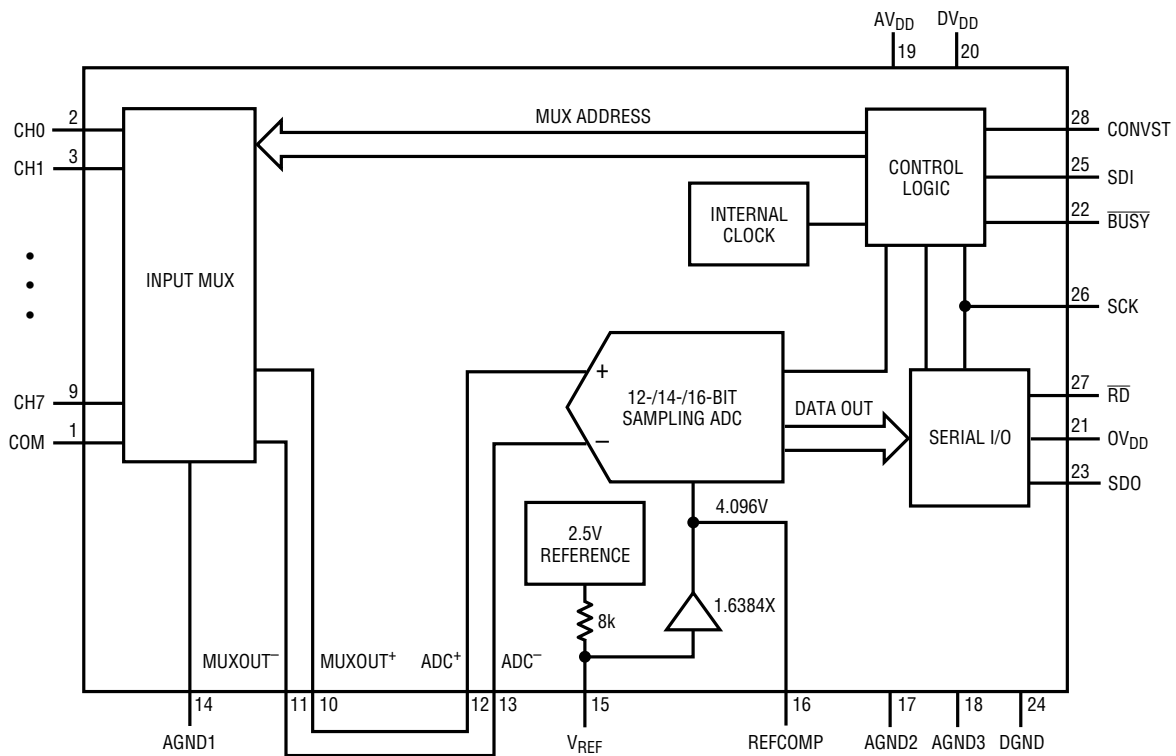
**SDI (Pin 25):** Serial Data Input.

**SCK (Pin 26):** Serial Data Clock.

**$\overline{RD}$  (Pin 27):** Read Input. This active low signal enables the digital output pin SDO and enables the serial interface, SDI and SCK are ignored when  $\overline{RD}$  is high.

**CONVST (Pin 28):** Conversion Start. The ADC starts a conversion on CONVST's rising edge.

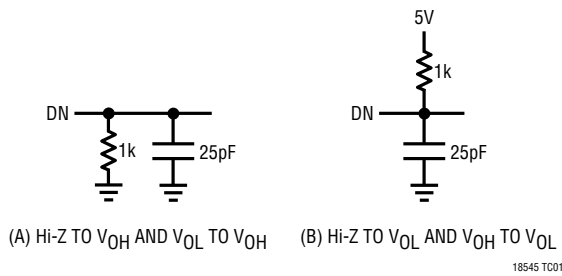
## FUNCTIONAL BLOCK DIAGRAM



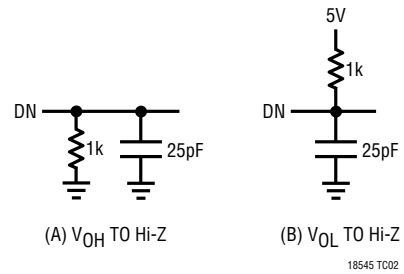
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## TEST CIRCUITS

### Load Circuits for Access Timing

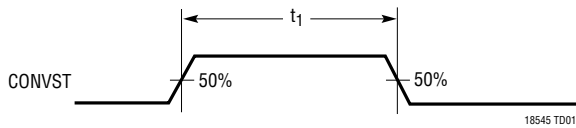


### Load Circuits for Output Float Delay

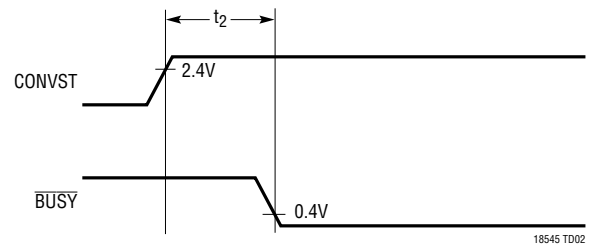


## TIMING DIAGRAMS

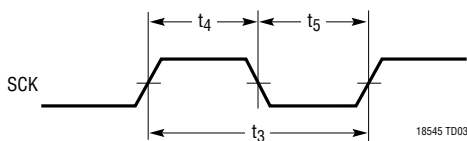
### $t_1$ (For Short Pulse Mode)



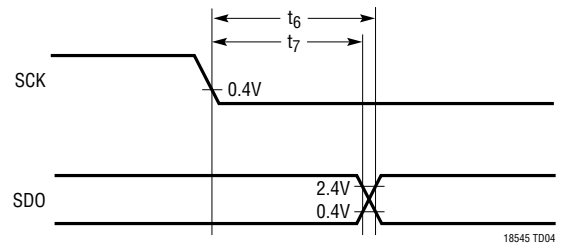
### $t_2$ (CONVST to $\overline{BUSY}$ Delay)



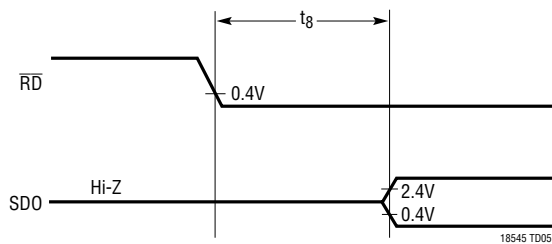
### $t_3, t_4, t_5$ (SCK Timing)



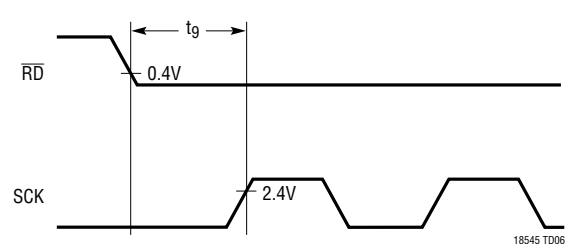
### $t_6$ (Delay Time, $SCK \downarrow$ to SDO Valid) $t_7$ (Time from Previous Data Remains Valid After $SCK \downarrow$ )



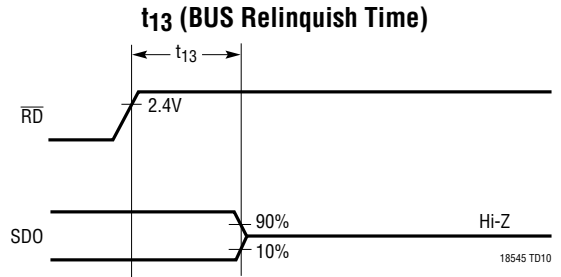
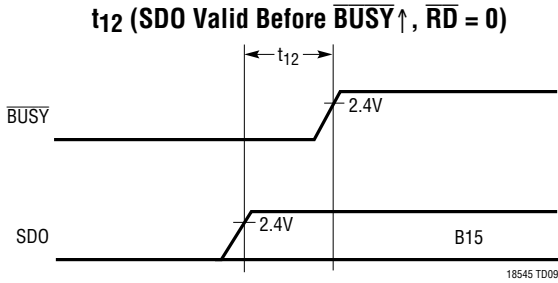
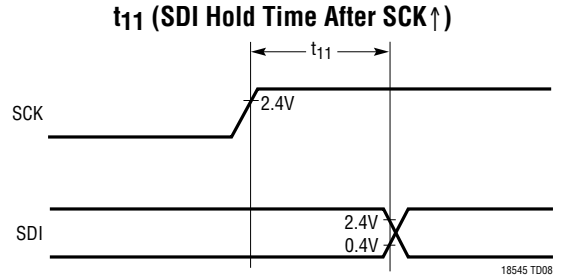
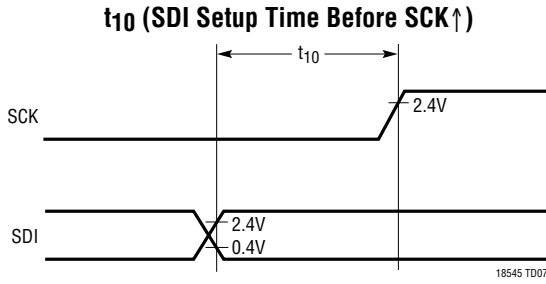
### $t_8$ (SDO Valid After $\overline{RD} \downarrow$ )



### $t_9$ ( $\overline{RD} \downarrow$ to SCK Setup Time)



**TIMING DIAGRAMS**



## APPLICATIONS INFORMATION

### OVERVIEW

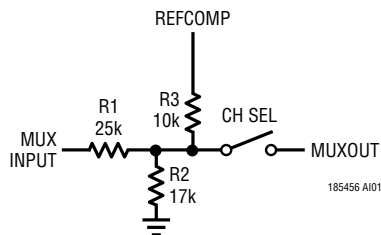
The LTC1854/LTC1855/LTC1856 are innovative, multi-channel ADCs. The on-chip resistors provide attenuation and offset for each channel. The precisely trimmed attenuators ensure an accurate input range. Because they precede the multiplexer, errors due to multiplexer on-resistance are eliminated.

The input word selects the single ended or differential inputs for each channel or pair of channels. Overrange protection is provided for unselected channels. An overrange condition on an unused channel will not affect the conversion result on the selected channel.

### CONVERSION DETAILS

The LTC1854/LTC1855/LTC1856 use a successive approximation algorithm and an internal sample-and-hold circuit to convert an analog signal to a 12-/14-/16-bit serial output respectively. The ADCs are complete with a precision reference and an internal clock. The control logic provides easy interface to microprocessors and DSPs. (Please refer to the Digital Interface section for the data format.)

The analog signals applied at the MUX input channels are rescaled by the resistor divider network formed by R1, R2 and R3 as shown below. The rescaled signals appear on the MUXOUT (Pins 10, 11) which are also connected to the ADC inputs (Pins 12, 13) under normal operation.



Before starting a conversion, an 8-bit data word is clocked into the SDI input on the first eight rising SCK edges to select the MUX address and power down mode. The ADC enters acquisition mode on the falling edge of the sixth clock in the 8-bit data word and ends on the rising edge of the CONVST signal which also starts a conversion (see Figure 7). A minimum time of 4 $\mu$ s will provide enough time for the sample-and-hold capacitors to acquire the analog signal. Once a conversion cycle has begun, it cannot be restarted.

During the conversion, the internal differential 12-/14-/16-bit capacitive DAC output is sequenced by the SAR from the most significant bit (MSB) to the least significant bit (LSB). The input is successively compared with the binary weighted charges supplied by the differential capacitive DAC. Bit decisions are made by a high speed comparator. At the end of a conversion, the DAC output balances the analog input ( $ADC^+ - ADC^-$ ). The SAR contents (a 12-/14-/16-bit data word) which represents the difference of  $ADC^+$  and  $ADC^-$  are loaded into the 12-/14-/16-bit shift register.

### DRIVING THE ANALOG INPUTS

The input range for the LTC1854/LTC1855/LTC1856 is  $\pm 10V$  and the MUX inputs are overvoltage protected to  $\pm 30V$ . The input impedance is typically 31k $\Omega$ ; therefore, it should be driven with a low impedance source. Wideband noise coupling into the input can be minimized by placing a 3000pF capacitor at the input as shown in Figure 2. An NPO-type capacitor gives the lowest distortion. Place the capacitor as close to the device input pin as possible. If an amplifier is to be used to drive the input, care should be taken to select an amplifier with adequate accuracy, linearity and noise for the application. The following list is a summary of the op amps that are suitable for driving the LTC1854/LTC1855/LTC1856. More detailed information is available in the Linear Technology data books and online at [www.linear.com](http://www.linear.com).

LT<sup>®</sup>1007: Low noise precision amplifier. 2.7mA supply current  $\pm 5V$  to  $\pm 15V$  supplies. Gain bandwidth product 8MHz. DC applications.

## APPLICATIONS INFORMATION

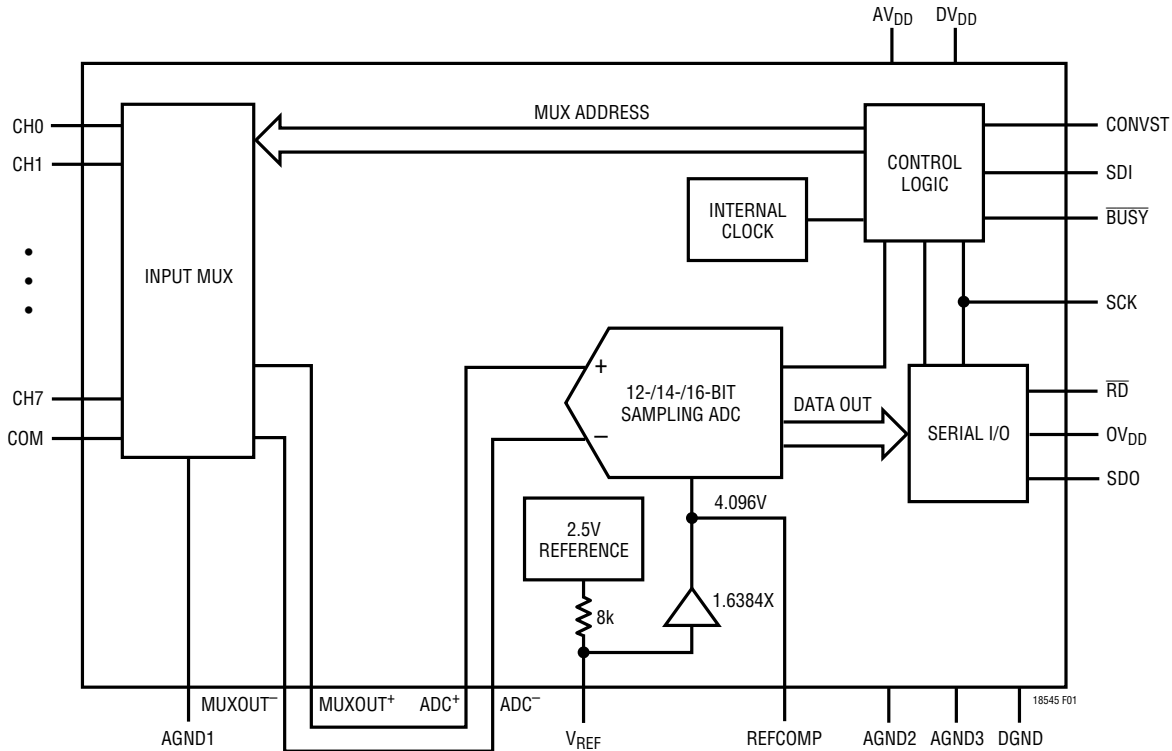


Figure 1. LTC1854/LTC1855/LTC1856 Simplified Equivalent Circuit

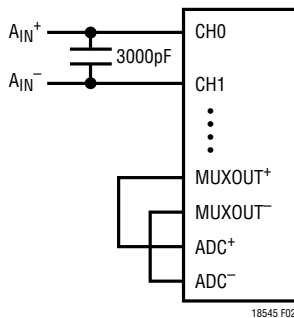


Figure 2. Analog Input Filtering

LT1227: 140MHz video current feedback amplifier. 10mA supply current.  $\pm 5V$  to  $\pm 15V$  supplies. Low noise and low distortion.

LT1468/LT1469: Single and dual 90MHz, 16-bit accurate op amp. Good AC/DC specs.  $\pm 5V$  to  $\pm 15V$  supplies.

LT1677: Single, low noise op amp. Rail-to-rail input and output. Up to  $\pm 15V$  supplies.

LT1792: Single, low noise JFET input op amp,  $\pm 5V$  supplies.

LT1793: Single, low noise JFET input op amp, 10pA bias current,  $\pm 5V$  supplies.

LT1881/LT1882: Dual and quad, 200pA bias current, rail-to-rail output op amps. Up to  $\pm 15V$  supplies.

LT1844/LT1885: Dual and quad, 400pA bias current, rail-to-rail output op amps. Up to  $\pm 15V$  supplies. Faster response and settling time.

### INTERNAL VOLTAGE REFERENCE

The LTC1854/LTC1855/LTC1856 have an on-chip, temperature compensated, curvature corrected, bandgap reference, which is factory trimmed to 2.50V. The full-scale range of the LTC1854/LTC1855/LTC1856 is equal to  $\pm 10V$ . The output of the reference is connected to the input of a gain of 1.6384x buffer through an 8k resistor (see Figure 3). The input to the buffer or the output of the reference

## APPLICATIONS INFORMATION

is available at  $V_{REF}$  (Pin 15). The internal reference can be overdriven with an external reference if more accuracy is needed. The buffer output drives the internal DAC and is available at REFCOMP (Pin 16). The REFCOMP pin can be used to drive a steady DC load of less than 2mA. Driving an AC load is not recommended because it can cause the performance of the converter to degrade.

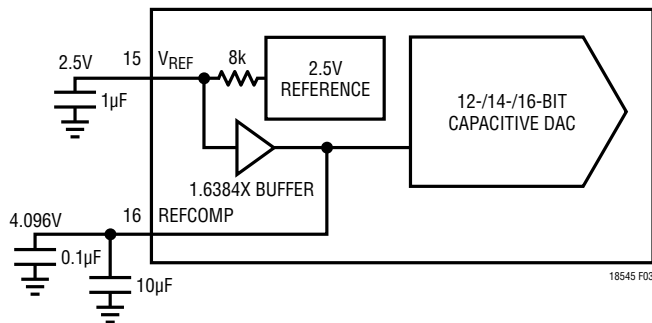


Figure 3. Internal or External Reference Source

For minimum code transition noise the  $V_{REF}$  pin and the REFCOMP pin should each be decoupled with a capacitor to filter wideband noise from the reference and the buffer.

## FULL SCALE AND OFFSET

Figure 4 shows the ideal input/output characteristics for the LTC1856. The code transitions occur midway be-

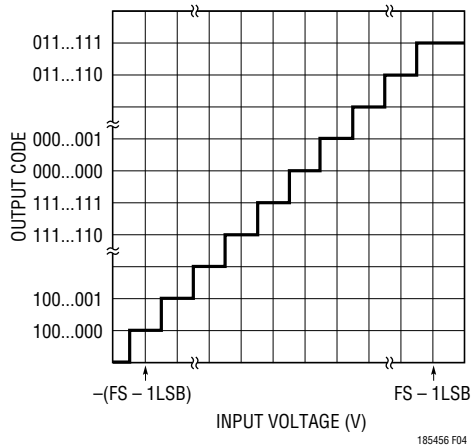


Figure 4. Bipolar Transfer Characteristics

tween successive integer LSB values (i.e.,  $-FS+0.5LSB$ ,  $-FS+1.5LSB$ ,  $-FS+2.5LSB$ , ...  $FS-1.5LSB$ ,  $FS-0.5LSB$ ). The output is two's complement binary with:

$$1 \text{ LSB} = \frac{FS - (-FS)}{65566} = \frac{20V}{65536} = 305.2\mu V$$

In applications where absolute accuracy is important, offset and full-scale errors can be adjusted to zero during a calibration sequence. Offset error must be adjusted before full-scale error. Zero offset is achieved by adjusting the offset applied to the “-” input. For single-ended inputs, this offset should be applied to the COM pin. For differential inputs, the “-” input is dictated by the MUX address.

For zero offset error, apply  $-0.5LSB$  to the “+” input and adjust the offset at the “-” input until the output code flickers between 0000 0000 0000 0000 and 1111 1111 1111 1111 for the LTC1856, between 00 0000 0000 0000 and 11 1111 1111 1111 for the LTC1855 and between 0000 0000 0000 and 1111 1111 1111 for the LTC1854.

For full-scale adjustment, an input voltage of  $FS - 1.5LSBs$  should be applied to the “+” input and the appropriate reference adjusted until the output code flickers between 0111 1111 1111 1110 and 0111 1111 1111 1111 for the LTC1856, between 01 1111 1111 1110 and 01 1111 1111 1111 for the LTC1855 and between 0111 1111 1110 and 0111 1111 1111 for the LTC1854.

These adjustments as well as the factory trims affect all channels. The channel-to-channel offset and gain error matching are guaranteed by design to meet the specifications in the Converter Characteristics table.

## APPLICATIONS INFORMATION

### DC PERFORMANCE

One way of measuring the transition noise associated with a high resolution ADC is to use a technique where a DC signal is applied to the input of the MUX and the resulting output codes are collected over a large number of conversions. For example in Figure 5 the distribution of output code is shown for a DC input that has been digitized 4096 times. The distribution is Gaussian and the RMS code transition is about 1LSB for the LTC1856.

### DIGITAL INTERFACE

#### Internal Clock

The ADC has an internal clock that is trimmed to achieve a typical conversion time of 4 $\mu$ s. No external adjustments are required and, with the maximum acquisition time of 4 $\mu$ s, throughput performance of 100ksps is assured.

#### 3V Input/Output Compatible

The LTC1854/LTC1855/LTC1856 operate on a 5V supply, which makes the devices easy to interface to 5V digital systems. These devices can also interface to 3V digital systems: the digital input pins (SCK, SDI, CONVST and  $\overline{RD}$ ) of the LTC1854/LTC1855/LTC1856 recognize 3V or 5V inputs. The LTC1854/LTC1855/LTC1856 have a dedicated

output supply pin ( $OV_{DD}$ ) that controls the output swings of the digital output pins (SDO,  $\overline{BUSY}$ ) and allows the part to interface to either 3V or 5V digital systems. The SDO output is two's complement.

#### Timing and Control

Conversion start and data read are controlled by two digital inputs: CONVST and  $\overline{RD}$ . To start a conversion and put the sample-and-hold into the hold mode bring CONVST high for at least 40ns. Once initiated it cannot be restarted until the conversion is complete. Converter status is indicated by the  $\overline{BUSY}$  output, which goes low while the conversion is in progress.

Figures 6a and 6b show two different modes of operation for the LTC1856. For the 12-bit LTC1854 and 14-bit LTC1855, the last four and two bits of the SDO will output zeros, respectively. In mode 1 (Figure 6a),  $\overline{RD}$  is tied low. The rising edge of CONVST starts the conversion. The data outputs are always enabled. The MSB of the data output is available after the conversion. In mode 2 (Figure 6b), CONVST and  $\overline{RD}$  are tied together. The rising edge of the CONVST signal starts the conversion. Data outputs are in three-state at this time. When the conversion is complete ( $\overline{BUSY}$  goes high), CONVST and  $\overline{RD}$  go low to enable the data output for the previous conversion.

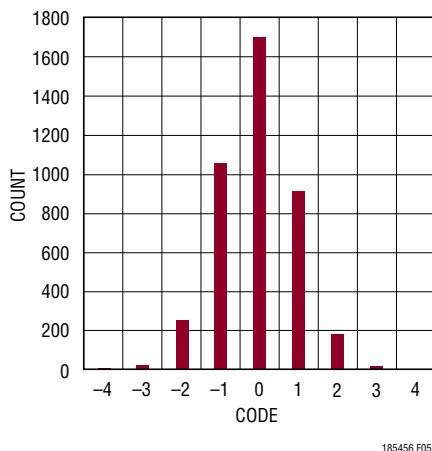


Figure 5. LTC1856 Histogram for 4096 Conversions



APPLICATIONS INFORMATION

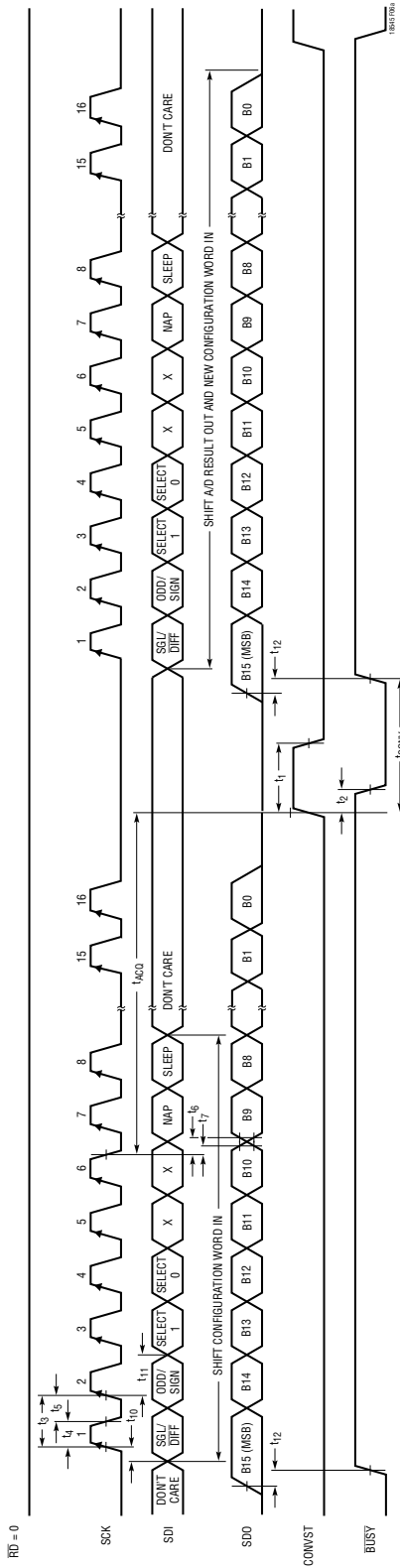


Figure 6a. Mode 1 for the LTC1856\*. CONVST Starts a Conversion, Data Output is Always Enabled (RD = 0)

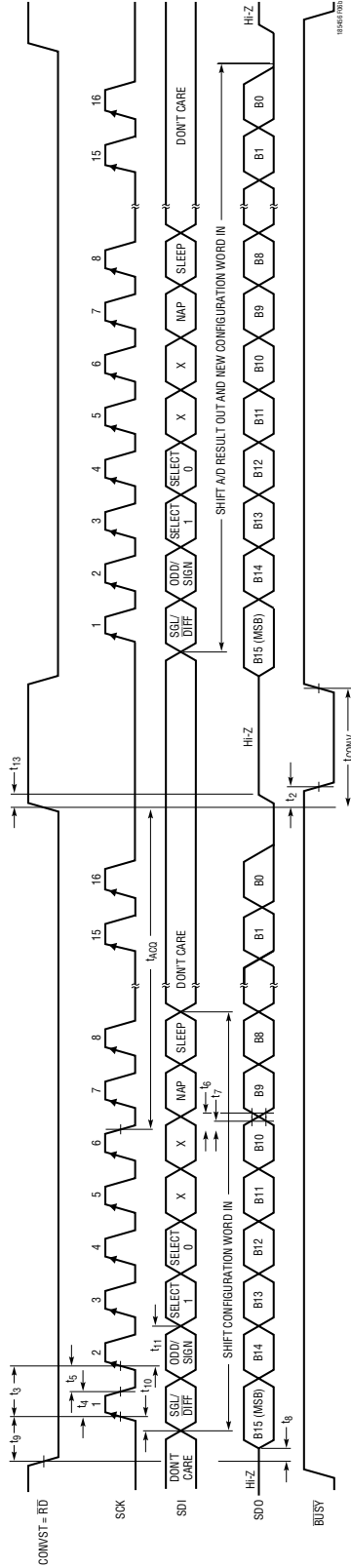


Figure 6b. Mode 2 for the LTC1856\*. CONVST and RD Tied Together. CONVST Starts a Conversion, Data is Read by RD

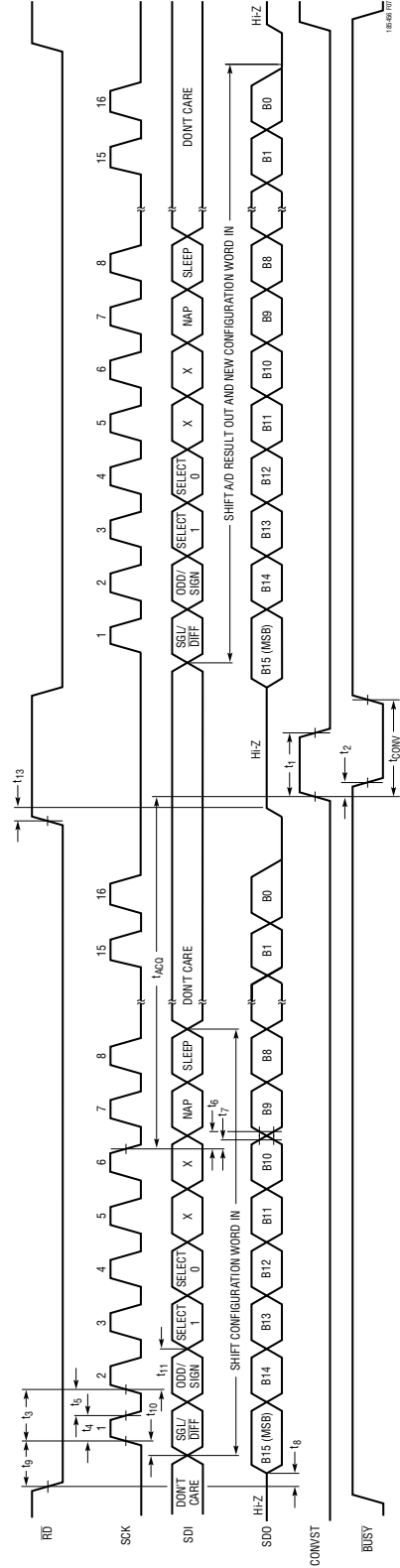


Figure 7. Operating Sequence for the LTC1855\*

\*For the 12-bit LTC1854 and the LTC1855 the last four and two bits of the SDO will output zeros, respectively.

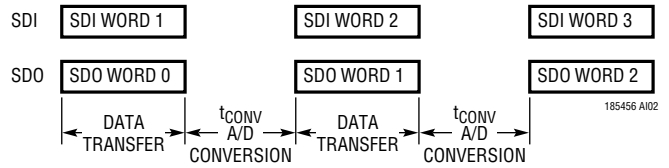
## APPLICATIONS INFORMATION

### SERIAL DATA INPUT (SDI) INTERFACE

The LTC1854/LTC1855/LTC1856 communicate with micro-processors and other external circuitry via a synchronous, full duplex, 3-wire serial interface (see Figure 7). The shift clock (SCK) synchronizes the data transfer with each bit being transmitted on the falling SCK edge and captured on the rising SCK edge in both transmitting and receiving systems. The data is transmitted and received simultaneously (full duplex).

An 8-bit input word is shifted into the SDI input which configures the LTC1854/LTC1855/LTC1856 for the next conversion. Simultaneously, the result of the previous conversion is output on the SDO line. At the end of the data exchange the requested conversion begins by applying a rising edge on CONVST. After  $t_{CONV}$ , the conversion is complete and the results will be available on the next data transfer cycle. As shown below, the result of a

conversion is delayed by one conversion from the input word requesting it.



### INPUT DATA WORD

The LTC1854/LTC1855/LTC1856 8-bit data word is clocked into the SDI input on the first eight rising SCK edges. Further inputs on the SDI pin are then ignored until the next conversion. The eight bits of the input word are defined as follows:

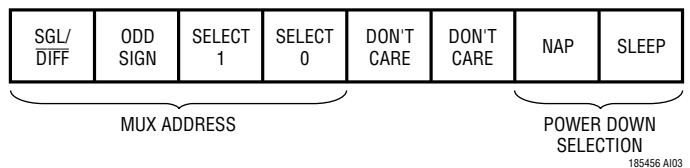


Table 1. Multiplexer Channel Selection

MUX ADDRESS			DIFFERENTIAL CHANNEL SELECTION								MUX ADDRESS			SINGLE-ENDED CHANNEL SELECTION								
SGL/DIFF	ODD SIGN	SELECT 1 0	0	1	2	3	4	5	6	7	SGL/DIFF	ODD SIGN	SELECT 1 0	0	1	2	3	4	5	6	7	COM
0	0	0 0	+	-							1	0	0 0	+								-
0	0	0 1			+	-					1	0	0 1			+						-
0	0	1 0					+	-			1	0	1 0					+				-
0	0	1 1								+	-	1	0	1 1						+		-
0	1	0 0	-	+								1	1	0 0		+						-
0	1	0 1			-	+						1	1	0 1			+					-
0	1	1 0					-	+				1	1	1 0					+			-
0	1	1 1							-	+		1	1	1 1							+	-

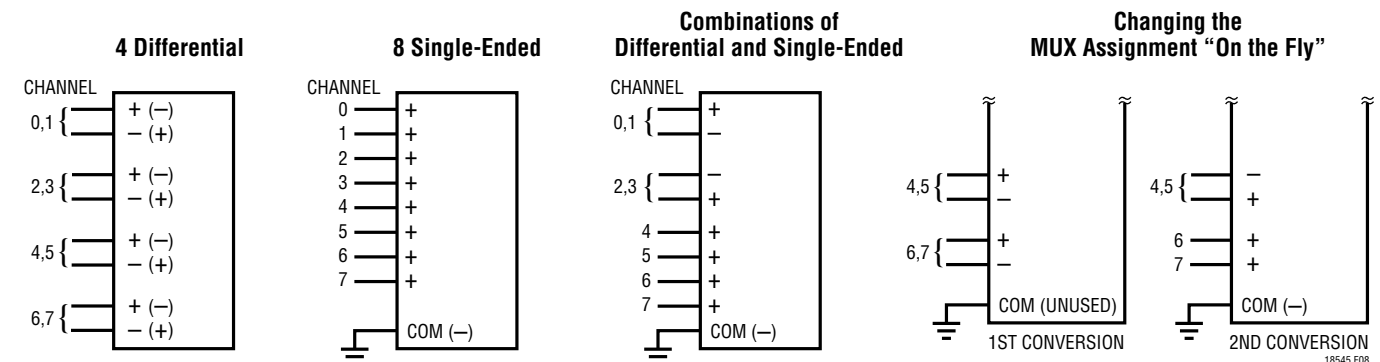


Figure 8. Examples of Multiplexer Options on the LTC1854/LTC1855/LTC1856

## APPLICATIONS INFORMATION

### MUX ADDRESS

The first four bits of the input word assign the MUX configuration for the requested conversion. For a given channel selection, the converter will measure the voltage between the two channels indicated by the + and – signs in the selected row of Table 1. Note that in differential mode (SGL/DIFF = 0) measurements are limited to four adjacent input pairs with either polarity. In single-ended mode, all input channels are measured with respect to COM. Both the “+” and “–” inputs are sampled simultaneously so common mode noise is rejected. Bits 5 and 6 of the input words are Don’t Care bits.

### POWER DOWN SELECTION (NAP, SLEEP)

The last two bits of the input word (Nap and Sleep) determine the power shutdown mode of the LTC1854/LTC1855/LTC1856. See Table 2. Nap mode is selected when Nap = 1 and Sleep = 0. The previous conversion result will be clocked out and a conversion will occur before entering the Nap mode. The Nap mode starts at the end of the conversion which is indicated by the rising edge of the  $\overline{\text{BUSY}}$  signal. Nap mode lasts until the falling edge of the 2nd SCK (see Figure 9). Automatic nap will be achieved if Nap = 1 is selected each time an input word is written to the ADC.

**Table 2. Power Down Selection**

NAP	SLEEP	POWER DOWN MODE
0	0	Power On
1	0	Nap
X	1	Sleep

Sleep mode will occur when Sleep = 1 is selected, regardless of the selection of the Nap input. The previous conversion result can be clocked out and the Sleep mode will start on the falling edge of the last (16th) SCK. Notice that the CONVST should stay either high or low in sleep mode (see Figure 10). To wake up from the sleep mode, apply a rising edge on the CONVST signal and then apply Sleep = 0 on the next SDI word and the part will wake up on the falling edge of the last (16th) SCK (see Figure 11).

In Sleep mode, all bias currents are shut down and only the power on reset circuit and leakage currents (about 10 $\mu$ A) remain. Sleep mode wake-up time is dependent on the value of the capacitor connected to the REFCOMP (Pin 16). The wake-up time is typically 40ms with the recommended 10 $\mu$ F capacitor connected on the REFCOMP pin.

### DYNAMIC PERFORMANCE

FFT (Fast Fourier Transform) test techniques are used to test the ADC’s frequency response, distortion and noise at the rated throughput. By applying a low distortion sine wave and analyzing the digital output using an FFT algorithm, the ADC’s spectral content can be examined for frequencies outside the fundamental. Figure 12 shows a typical LTC1856 FFT plot which yields a SINAD of 87dB and THD of –101dB.

APPLICATIONS INFORMATION

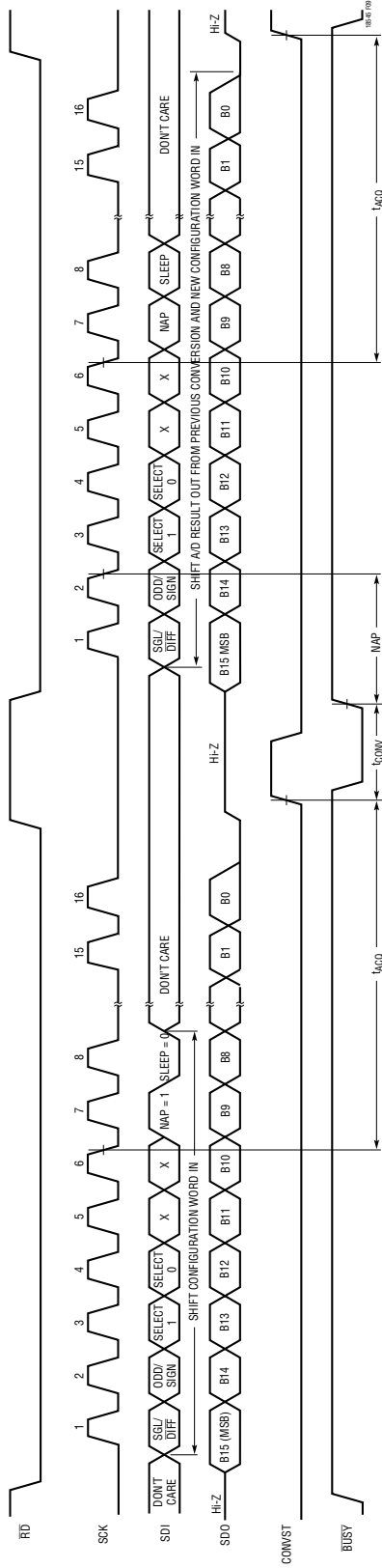


Figure 9. Nap Mode Operation for the LTC1856\*

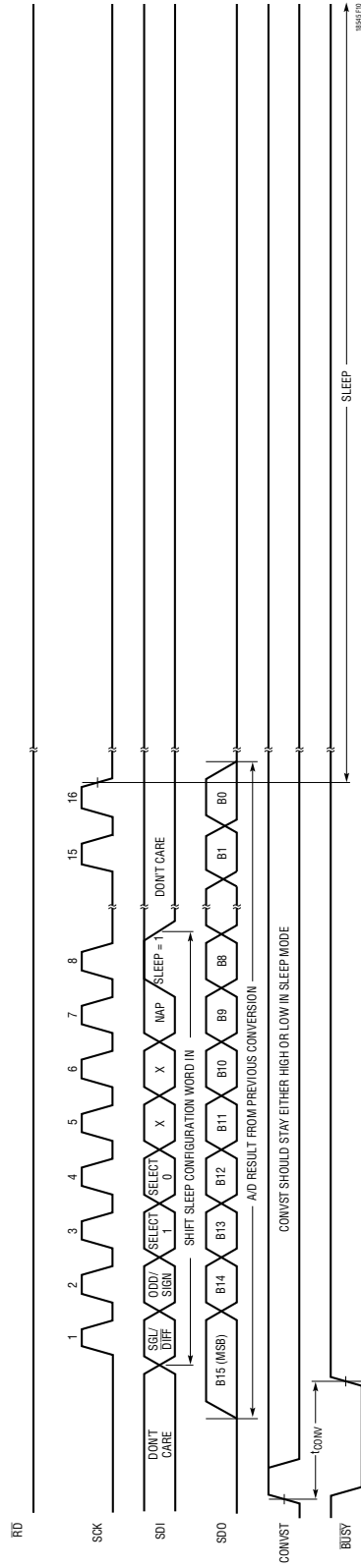


Figure 10. Sleep Mode Operation for the LTC1856\*

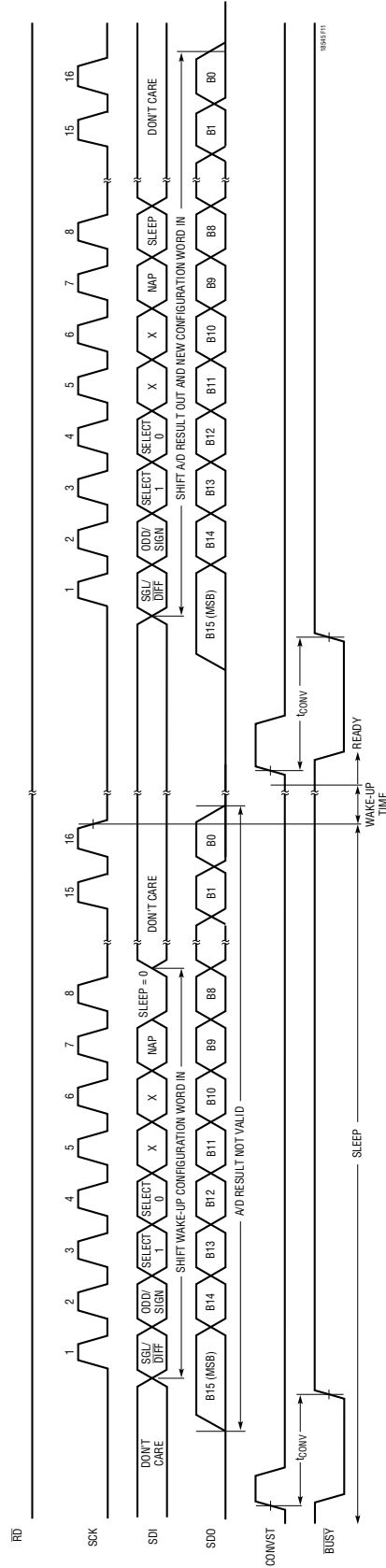


Figure 11. Wake Up from Sleep Mode for the LTC1856\*

\*For the 12-bit LTC1854 and the LTC1855 the last four and two bits of the SDO will output zeros, respectively.

## APPLICATIONS INFORMATION

### SIGNAL-TO-NOISE AND DISTORTION RATIO

The Signal-to-Noise and Distortion Ratio (SINAD) is the ratio between the RMS amplitude of the fundamental input frequency to the RMS amplitude of all other frequency components at the A/D output. The output is band limited to frequencies from above DC and below half the sampling frequency. Figure 12 shows a typical SINAD of 87dB with a 100kHz sampling rate and a 1kHz input.

### TOTAL HARMONIC DISTORTION

Total Harmonic Distortion (THD) is the ratio of the RMS sum of all harmonics of the input signal to the fundamental itself. The out-of-band harmonics alias into the frequency band between DC and half the sampling frequency. THD is expressed as:

$$\text{THD} = 20\log \frac{\sqrt{V_2^2 + V_3^2 + V_4^2 \dots + V_N^2}}{V_1}$$

where  $V_1$  is the RMS amplitude of the fundamental frequency and  $V_2$  through  $V_N$  are the amplitudes of the second through Nth harmonics.

### BOARD LAYOUT, POWER SUPPLIES AND DECOUPLING

Wire wrap boards are not recommended for high resolution or high speed A/D converters. To obtain the best performance from the LTC1854/LTC1855/LTC1856, a printed circuit board is required. Layout for the printed circuit board should ensure the digital and analog signal lines are separated as much as possible. In particular, care should be taken not to run any digital track alongside an analog signal track or underneath the ADC. The analog input should be screened by AGND.

In applications where the MUX is connected to the ADC, it is possible to get noise coupling into the ADC from the trace connecting the MUXOUT to the ADC. Therefore, reducing the length of the traces connecting the MUXOUT pins (Pins 10, 11) to the ADC pins (Pins 12, 13) can minimize the problem. The unused MUX inputs should be grounded to prevent noise coupling into the inputs.

Figure 13 shows the power supply grounding that will help obtain the best performance from the 12-bit/14-bit/16-bit ADCs. Pay particular attention to the design of the analog and digital ground planes. The DGND pin of the LTC1854/

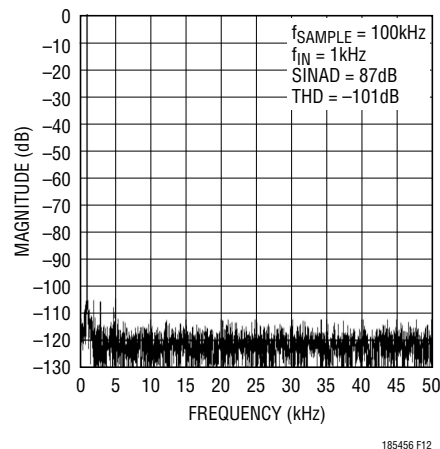


Figure 12. LTC1856 Nonaveraged 4096 Point FFT Plot

## APPLICATIONS INFORMATION

LTC1855/LTC1856 can be tied to the analog ground plane. Placing the bypass capacitor as close as possible to the power supply pins, the reference and reference buffer output is very important. Low impedance common returns for these bypass capacitors are essential to low noise operation of the ADC, and the foil width for these tracks should be as wide as possible. Also, since any potential difference in

grounds between the signal source and ADC appears as an error voltage in series with the input signal, attention should be paid to reducing the ground circuit impedance as much as possible. The digital output latches and the onboard sampling clock have been placed on the digital ground plane. The two ground planes are tied together at the ADC through a wide, low inductance path.

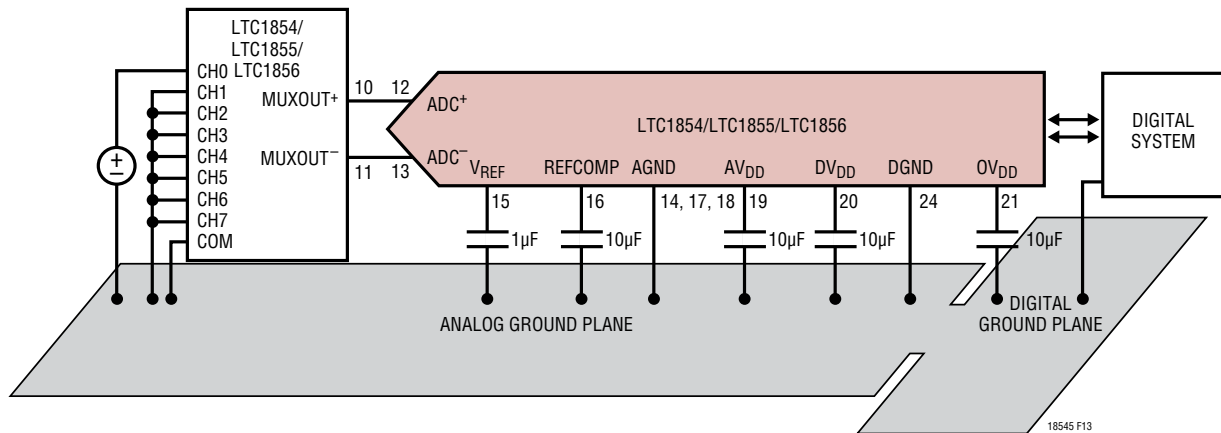
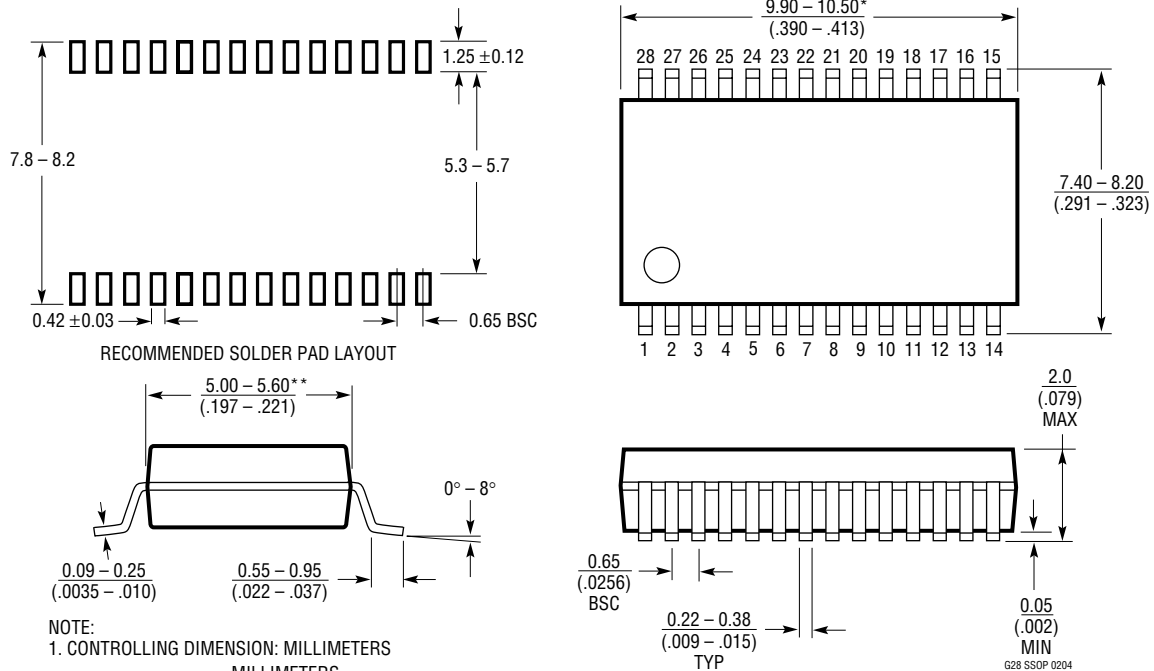


Figure 13. Power Supply Grounding Practice

**PACKAGE DESCRIPTION**

**G Package**  
**28-Lead Plastic SSOP (5.3mm)**  
 (Reference LTC DWG # 05-08-1640)



- NOTE:
1. CONTROLLING DIMENSION: MILLIMETERS
  2. DIMENSIONS ARE IN MILLIMETERS (INCHES)
  3. DRAWING NOT TO SCALE
- \*DIMENSIONS DO NOT INCLUDE MOLD FLASH. MOLD FLASH SHALL NOT EXCEED .152mm (.006") PER SIDE
- \*\*DIMENSIONS DO NOT INCLUDE INTERLEAD FLASH. INTERLEAD FLASH SHALL NOT EXCEED .254mm (.010") PER SIDE

