



## MULTIPLIER-DIVIDER

### FEATURES

- LOW COST
- DIFFERENTIAL INPUT
- ACCURACY 100% TESTED AND GUARANTEED
- LOW NOISE  
120 $\mu$ V, rms, 10Hz to 10kHz
- SELF-CONTAINED  
No additional amplifiers
- SMALL SIZE  
Hermetic TO-100 package
- WIDE TEMPERATURE OPERATION

### APPLICATIONS

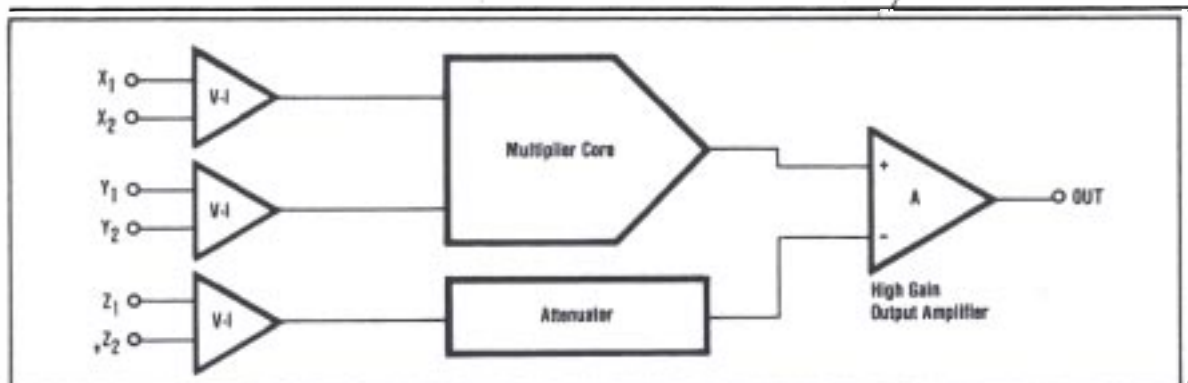
- MULTIPLICATION
- DIVISION
- SQUARING
- SQUARE ROOT
- LINEARIZATION
- POWER COMPUTATION
- ANALOG SIGNAL PROCESSING
- ALGEBRAIC COMPUTATION
- TRUE RMS-TO-DC CONVERSION

### DESCRIPTION

The 4213 multiplier-divider is a low cost precision device designed for general purpose application. In addition to four-quadrant multiplication, it also performs analog square root and division without the bother of external amplifiers. The 4213 is laser-trimmed to guarantee its rated accuracy with no

external components. The internal zener regulated references make the 4213 much less sensitive to supply variation than earlier IC multipliers. Hermetic TO-100 package, wide operating temperature range, low output noise, and low cost are some of the desirable features of this versatile device.

4213 FUNCTIONAL DIAGRAM



# SPECIFICATIONS

## ELECTRICAL

Specifications at  $T_A = +25^\circ\text{C}$  and  $\pm V_{CC} = 15\text{VDC}$  unless otherwise noted.

MODEL	PARAMETER	CONDITIONS	4213AM			4213BM			4213SM			UNITS
			MIN	TYP	MAX	MIN	TYP	MAX	MIN	TYP	MAX	
<b>MULTIPLIER PERFORMANCE</b>												
	Transfer Function		$\frac{(X_1 - X_2)(Y_1 - Y_2) + Z_2}{10}$				*			*		
	Total Error	$-10\text{V} \leq X, Y \leq 10\text{V}$ $T_A = +25^\circ\text{C}$			$\pm 1.0$						$\pm 0.5$	% FSR
	Initial	$-25^\circ\text{C} \leq T_A \leq +85^\circ\text{C}$		$\pm 0.008$	$\pm 0.02$		*					% FSR/ $^\circ\text{C}$
	vs Temperature	$-55^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		--	--		*					% FSR/ $^\circ\text{C}$
	vs Supply			$\pm 0.05$			*		$\pm 0.025$		$\pm 0.05$	% FSR/%
<b>Individual Errors</b>												
	Output Offset											mV
	Initial	$T_A = +25^\circ\text{C}$		$\pm 10$	$\pm 50$		$\pm 7$		$\pm 7$		$\pm 25$	mV/ $^\circ\text{C}$
	vs Temperature	$-25^\circ\text{C} \leq T_A \leq +85^\circ\text{C}$		$\pm 0.7$	$\pm 2.0$		$\pm 0.3$		$\pm 0.7$		--	mV/ $^\circ\text{C}$
	vs Temperature	$-55^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		--	--		*					mV/ $^\circ\text{C}$
	vs Supply			$\pm 0.25$			*		$\pm 0.3$		$\pm 0.7$	mV/%
	Scale Factor Error											% FSR
	Initial	$T_A = +25^\circ\text{C}$		$\pm 0.12$			*					% FSR
	vs Temperature	$-25^\circ\text{C} \leq T_A \leq +85^\circ\text{C}$		$\pm 0.008$			*					% FSR/ $^\circ\text{C}$
	vs Temperature	$-55^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		--	--		*		$\pm 0.008$			% FSR/ $^\circ\text{C}$
	vs Supply			$\pm 0.05$			*					% FSR/%
	Nonlinearity						*					% FSR
	X Input	$X = 20\text{V}, \text{p-p}; Y = \pm 10\text{VDC}$		$\pm 0.08$			*					% FSR
	Y Input	$Y = 20\text{V}, \text{p-p}; X = \pm 10\text{VDC}$		$\pm 0.01$			*					% FSR
	Feedthrough	$f = 50\text{Hz}$					*					mV, p-p
	X Input	$X = 20\text{V}, \text{p-p}; Y = 0$		30			*					mV, p-p
	Y Input	$Y = 20\text{V}, \text{p-p}; X = 0$		6			*					mV, p-p/ $^\circ\text{C}$
	vs Temperature	$-25^\circ\text{C} \leq T_A \leq +85^\circ\text{C}$		0.1			*			0.1		mV, p-p/ $^\circ\text{C}$
	vs Temperature	$-55^\circ\text{C} \leq T_A \leq +125^\circ\text{C}$		--	--		*					mV, p-p/ $^\circ\text{C}$
	vs Supply			0.15			*					mV, p-p/%
<b>DIVIDER PERFORMANCE</b>												
	Transfer Function	$X_1 > X_2$		$\frac{10(Z_1 - Z_2)}{(X_1 - X_2)} + Y_2$				*			*	
	Total Error (with external adjustments)	$X = -10\text{V}$ $-10\text{V} \leq Z \leq +10\text{V}$ $X = -1\text{V}$ $-1\text{V} \leq Z \leq +1\text{V}$ $-10\text{V} \leq X \leq -0.2\text{V}$ $-10\text{V} \leq Z \leq +10\text{V}$		$\pm 0.75$				$\pm 0.35$		$\pm 0.35$		% FSR
				$\pm 2.0$				$\pm 1.0$		$\pm 1.0$		% FSR
				$\pm 5.0$				$\pm 1.0$		$\pm 1.0$		% FSR
<b>SQUARER PERFORMANCE</b>												
	Transfer Function			$\frac{(X_1 - X_2)^2 + Z_2}{10}$				*			*	
	Total Error	$-10\text{V} \leq X \leq +10\text{V}$		$\pm 0.6$				$\pm 0.3$		$\pm 0.3$		% FSR
<b>SQUARE-ROOTER PERFORMANCE</b>												
	Transfer Function	$Z_1 < Z_2$		$+\sqrt{10(Z_2 - Z_1)}$				*			*	
	Total Error	$1\text{V} \leq Z \leq 10\text{V}$		$\pm 1$				$\pm 0.5$		$\pm 0.5$		% FSR
<b>AC PERFORMANCE</b>												
	Small-Signal Bandwidth	$\pm 3\text{dB}$		550				*		*		kHz
	1% Amplitude Error	Small Signal		70				*		*		kHz
	1% (0.57°) Vector Error	Small Signal		5				*		*		kHz
	Full Power Bandwidth	$ V_d  = 10\text{V}, R_L = 2\text{k}\Omega$		320				*		*		kHz
	Slew Rate	$ V_d  = 10\text{V}, R_L = 2\text{k}\Omega$		20				*		*		V/ $\mu\text{sec}$
	Settling Time	$e = \pm 1\%, \Delta V_0 = 20\text{V}$		2				*		*		$\mu\text{sec}$
	Overload Recovery	50% Output Overload		0.2				*		*		$\mu\text{sec}$
<b>INPUT CHARACTERISTICS</b>												
	Input Voltage Range			$\pm 10$				*		*		V
	Rated Operation					$\pm V_{CC}$		*		*		V
	Absolute Maximum							*		*		V
	Input Resistance	X, Y, Z <sup>(1)</sup>		10				*		*		M $\Omega$
	Input Bias Current	X, Y, Z		1.4				*		*		$\mu\text{A}$
<b>OUTPUT CHARACTERISTICS</b>												
	Rated Output Voltage	$I_o = \pm 5\text{mA}$		$\pm 10$				*		*		V
	Current	$V_o = \pm 10\text{V}$		$\pm 5$				*		*		mA
	Output Resistance	$I = \text{DC}$		1.5				*		*		$\Omega$
		$X = Y = 0$						*		*		
				40				*		*		$\mu\text{V}/\sqrt{\text{Hz}}$
				1.0				*		*		$\mu\text{V}/\sqrt{\text{Hz}}$
				1060				*		*		Hz
				125				*		*		$\mu\text{V}, \text{rms}$
				3				*		*		mV, rms
<b>MENTS</b>												
	Rated Voltage			$\pm 15$				*		*		VDC
	Operating Range	Derated Performance		$\pm 8.5$		$\pm 20$		*		*		VDC
	Quiescent Current			$\pm 5.5$				*		*		mA

**NOTES:**

1.  $Z_2$  input resistance is  $10M\Omega$ , typical, with Pin 9 open. If Pin 9 is grounded or used for optional offset adjustment, the  $Z_2$  input resistance may be as low as  $25k\Omega$ .

\*Same as 4213AM specification.

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## TYPICAL PERFORMANCE CURVES

### NOTES:

1. Package must be derated based on:  $\theta_{JC} = 55^{\circ}\text{C/W}$  and  $\theta_{JA} = 165^{\circ}\text{C/W}$ .
2. For supply voltages less than  $\pm 20\text{VDC}$  the absolute maximum input voltage is equal to the supply voltage.
3. Short-circuit may be to ground only. Rating applies to  $+85^{\circ}\text{C}$  ambient.

## DEFINITIONS

### TOTAL ERROR (Accuracy)

Total error is the actual departure of the multiplier output voltage from the ideal product of its input voltages. It includes the sum of the effects of input and output DC offsets, gain error and nonlinearity.

### OUTPUT OFFSET

Output offset is the output voltage when both inputs  $V_X$  and  $V_Y$  are zero volts.

### SCALE FACTOR ERROR

Scale factor error is the difference between the actual scale factor and the ideal scale factor.

### NONLINEARITY

Nonlinearity is the maximum deviation from a best straightline (curve fitting on input-output graph) expressed as a percent of peak-to-peak full scale output.

### FEEDTHROUGH

Feedthrough is the signal at the output for any value of  $V_X$  or  $V_Y$  within the rated range, when the other input is zero.

### SMALL SIGNAL BANDWIDTH

Small signal bandwidth is the frequency at which the output is down 3dB from its low frequency value for a nominal output amplitude of 10% of full scale.

### 1% AMPLITUDE ERROR

The 1% amplitude error is the frequency the output amplitude is in error by 1%, measured with an output amplitude of 10% of full scale.

### 1% VECTOR ERROR

The 1% vector error is the frequency at which a phase error of 0.01 radians ( $0.57^\circ$ ) occurs. This is the most sensitive measure of dynamic error of a multiplier.

## APPLICATIONS INFORMATION

### MULTIPLICATION

Figure 1 shows the basic connection for four-quadrant multiplication.

The 4213 meets all of its specifications without trimming. Accuracy can, however, be improved by nulling the output offset voltage using the 100k $\Omega$  optional balance potentiometer shown in Figure 1.

AC feedthrough may be reduced to a minimum by applying an external voltage to the X or Y input as shown in Figure 2.

$Z_2$ , the optional summing input, may be used to sum a voltage into the output of the 4213. If not used, this

terminal, as well as the X and Y input terminals, should be grounded. All inputs should be referenced to power supply common.

Figure 3 shows how to achieve a scale factor larger than the nominal 0.1. In this case, the scale factor is unity which makes the transfer function

$$V_o = KV_X V_Y = K(X_1 - X_2)(Y_1 - Y_2)$$

$$K = [1 + (R_1/R_2)]/10$$

$$0.1 \leq K \leq 1$$

FIGURE 1 Multiplier Connection.

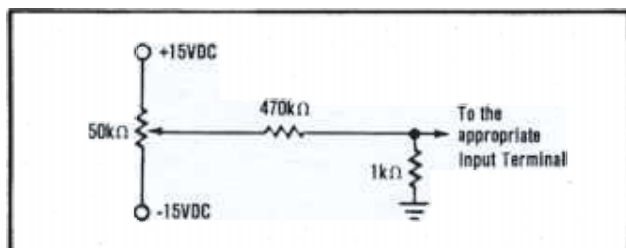


FIGURE 2. Optional Trimming Configuration.

FIGURE 3. Connection For Unity Scale Factor.

This circuit has the disadvantage of increasing the output offset voltage by a factor of 10 which may require the use of the optional balance control for some applications. In addition, this connection reduces the small signal bandwidth to about 50kHz.

### DIVISION

Figure 4 shows the basic connection for two-quadrant division. This configuration is a multiplier-inverted analog divider, i.e., a multiplier connected in the feedback loop of an operational amplifier. In the case of the 4213 this operational amplifier is the output amplifier of the multiplier itself.

#### FIGURE 4. Divider Connection.

The divider error with a multiplier-inverted analog divider is approximately

$$\epsilon_{\text{divider}} = 10 \epsilon_{\text{multiplier}} / (X_1 - X_2).$$

It is obvious from this error equation that divider error becomes excessively large for small values of  $X_1 - X_2$ . A 10-to-1 denominator range is usually the practical limit. If more accurate division is required over a wide range of denominator voltages, an externally generated voltage may be applied to the unused X-input (see Optional Trim Configuration). To trim, apply a ramp of +100mV to +1V at 100Hz to both  $X_1$  and  $Z_1$  if  $X_2$  is used for offset adjustment, otherwise reverse the signal polarity, and adjust the trim voltage to minimize the variation in the output. An alternative to this procedure would be to use the Burr-Brown DIV100, a precision log-antilog divider.

#### SQUARING

#### FIGURE 5. Squarer Connection.

#### SQUARE ROOT

Figure 6 shows the connection for taking the square root of the voltage  $V_z$ . The diode prevents a latching condition which could occur if the input momentarily changed polarity. This latching condition is not a design flaw in the 4213, but occurs when a multiplier is connected in the feedback loop of an operational amplifier to perform square root functions.

The load resistance  $R_L$  must be in the range of  $10\text{k}\Omega \leq R_L \leq 1\text{M}\Omega$ . This resistance must be in the circuit as it provides the current necessary to operate the diode.

The output offset should be nulled for optimum performance by allowing the input to be its smallest expected value and adjusting  $R_L$  for the proper output voltage.

#### Figure 7. Square Root Connection.

This will improve the square root mode accuracy to about that of the multiply mode.

#### BRIDGE LINEARIZATION

#### FIGURE 7. Bridge Linearization.

The use of the 4213 and the instrumentation amplifier to linearize the output from a bridge circuit makes the output  $V_o$  independent of the bridge supply voltage.

#### TRUE RMS-TO-DC CONVERSION

#### FIGURE 8. True RMS-to-DC Conversion.

The RMS-to-DC conversion circuit of Figure 8 gives greater accuracy and bandwidth but with less dynamic range than most rms-to-DC converters.

### PERCENTAGE COMPUTATION

FIGURE 9. Percentage Computation.

The circuit of Figure 9 has a sensitivity of 1V/% and is capable of measuring 10% deviations. Wider deviation can be measured by decreasing the ratio of  $R_2/R_1$ .

### SINE FUNCTION GENERATOR

FIGURE 10. Sine Function Generator.

The circuit in Figure 10 uses implicit feedback to implement the following sine function approximation:

$$\begin{aligned} V_o &= (1.5715V_1 - 0.004317V_1^3)/(1 + 0.001398V_1^2) \\ &= 10 \sin(9V_1). \end{aligned}$$

### SINGLE-PHASE POWER MEASUREMENT

FIGURE 11. Single-Phase Instantaneous and Real Power Measurement.

### WIRING PRECAUTIONS

In order to prevent frequency instability due to lead inductance of the power supply lines, each power supply should be bypassed. This should be done by connecting a 10 $\mu$ F tantalum capacitor in parallel with a 1000pF ceramic capacitor from the +V<sub>CC</sub> and -V<sub>CC</sub> pins of the 4213 to the power supply common. The connection of these capacitors should be as close to the 4213 as practical.

### CAPACITIVE LOADS

Stable operation is maintained with capacitive loads to 1000pF in all modes typically, except the square root mode for which 50pF is a safe upper limit. Higher capacitive loads can be driven if a 100 $\Omega$  resistor is connected in series with the 4213's output.

### MORE CIRCUITS

The theory and procedures for developing virtually any function generator or linearization circuit can be found in the Burr-Brown/ McGraw Hill book "FUNCTION CIRCUITS - Design and Applications."

**PACKAGING INFORMATION**

ORDERABLE DEVICE	STATUS(1)	PACKAGE TYPE	PACKAGE DRAWING	PINS	PACKAGE QTY
4213AM	NRND	TO/SOT	LME	10	20
4213AM2	OBSOLETE	TO/SOT	LMC	8	
4213BM	NRND	TO/SOT	LME	10	20
4213BM1	OBSOLETE	TO/SOT	LMC	8	
4213SM	NRND	TO/SOT	LME	10	20

(1) The marketing status values are defined as follows:

**ACTIVE:** Product device recommended for new designs.

**LIFEBUY:** TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

**NRND:** Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

**PREVIEW:** Device has been announced but is not in production. Samples may or may not be available.

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Mailing Address: Texas Instruments  
Post Office Box 655303 Dallas, Texas 75265

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